



# TS4984

## 2 x 1W Stereo audio power amplifier with active low standby mode

- Operating from  $V_{CC}=2.2V$  to  $5.5V$
- 1W output power per channel @  $V_{CC}=5V$ , THD+N=1%,  $R_L=8\Omega$
- 10nA standby current
- 62dB PSRR @ 217Hz with grounded inputs
- High SNR: 100dB(A) typ.
- Near-zero pop & click
- Available in QFN16 4x4 mm, 0.5mm pitch, leadfree package

### Description

The TS4984 has been designed for top of the class stereo audio applications. Thanks to its compact and power dissipation efficient QFN package, it suits various applications.

With a BTL configuration, this Audio Power Amplifier is capable of delivering 1W per channel of continuous RMS output power into an  $8\Omega$  load @ 5V.

An externally controlled standby mode control reduces the supply current to less than 10nA per channel. The device also features an internal thermal shutdown protection.

The gain of each channel can be configured by external gain setting resistors.

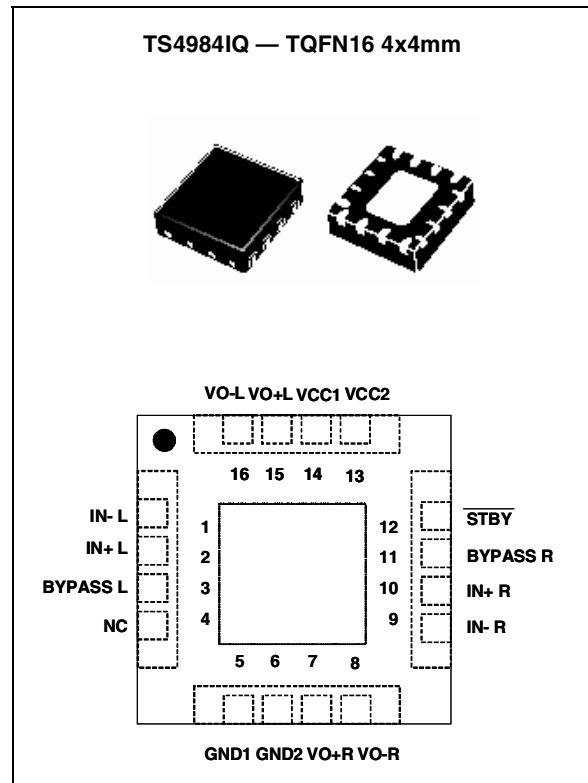
### Applications

- Cellular mobile phones
- Notebook computers & PDAs
- LCD monitors & TVs
- Portable audio devices

### Order Codes

Part Number	Temperature Range	Package	Packaging	Marking
TS4984IQT	-40, +85°C	QFN	Tape & Reel	K984

### Pin Connections (top view)



### 1 Typical Application

Figure 1 shows a schematic view of a typical audio amplification application using the TS4984. Table 1 describes the components used in this typical application.

Figure 1: Typical application schematic

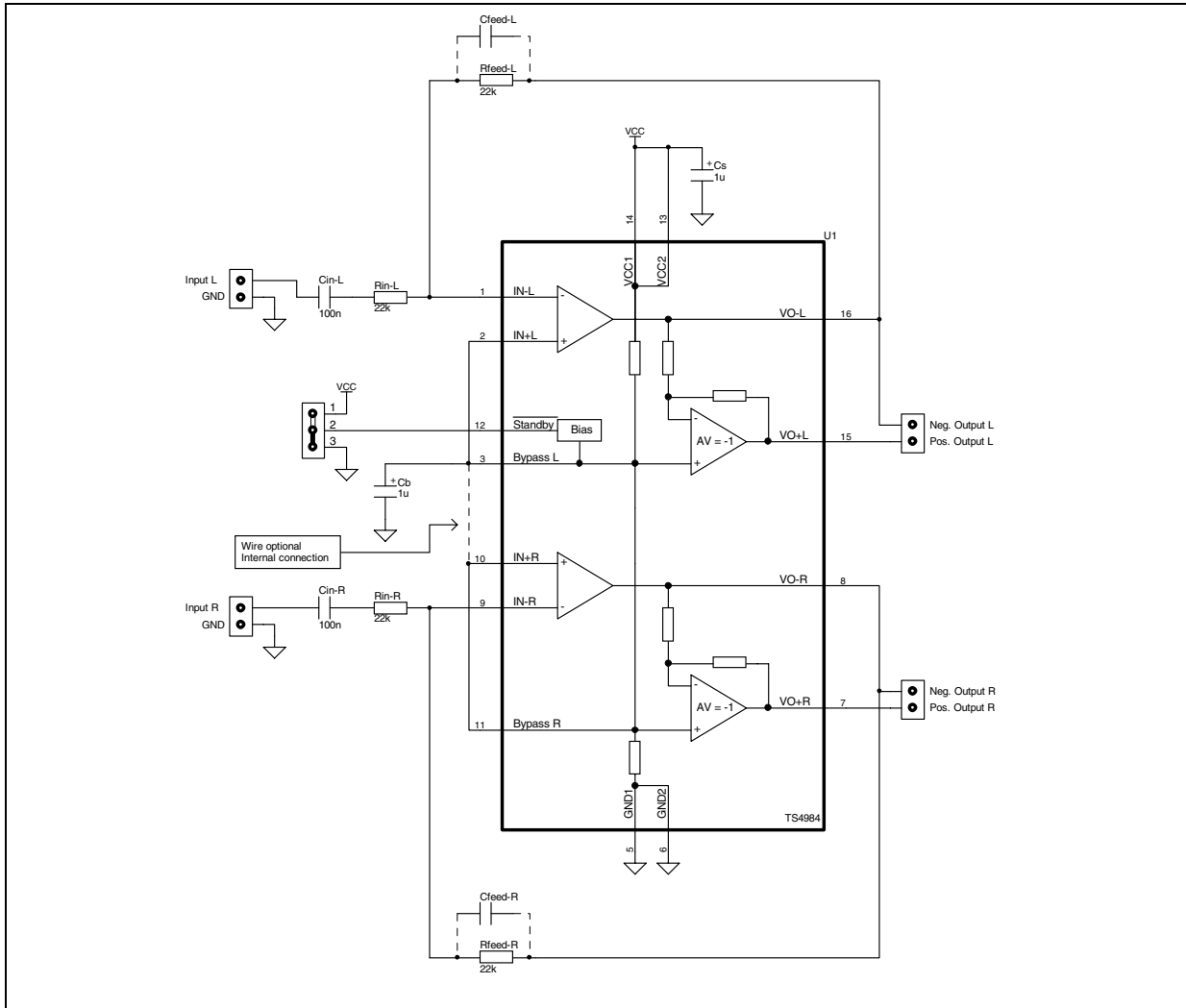


Table 1: External component descriptions

Components	Functional Description
$R_{IN\ L,R}$	Inverting input resistors which sets the closed loop gain in conjunction with $R_{feed}$ . These resistors also form a high pass filter with $C_{IN}$ ( $f_c = 1 / (2 \times \pi \times R_{IN} \times C_{IN})$ ).
$C_{IN\ L,R}$	Input coupling capacitors which blocks the DC voltage at the amplifier input terminal.
$R_{FEED\ L,R}$	Feedback resistors which sets the closed loop gain in conjunction with $R_{IN}$ .
$C_S$	Supply Bypass capacitor which provides power supply filtering.
$C_B$	Bypass pin capacitor which provides half supply filtering.
$A_{V\ L,R}$	Closed loop gain in BTL configuration = $2 \times (R_{FEED} / R_{IN})$ on each channel.

2 Absolute maximum ratings and operating conditions

Table 2: Key parameters and their absolute maximum ratings

Symbol	Parameter	Value	Unit
V <sub>CC</sub>	Supply voltage <sup>1</sup>	6	V
V <sub>i</sub>	Input Voltage <sup>2</sup>	GND to V <sub>CC</sub>	V
T <sub>oper</sub>	Operating Free Air Temperature Range	-40 to + 85	°C
T <sub>stg</sub>	Storage Temperature	-65 to +150	°C
T <sub>j</sub>	Maximum Junction Temperature	150	°C
R <sub>thja</sub>	Thermal Resistance Junction to Ambient QFN16	120	°C/W
P <sub>d</sub>	Power Dissipation	Internally Limited	
ESD	Human Body Model <sup>3</sup>	2	kV
ESD	Machine Model	200	V
	Latch-up Immunity	200mA	

- 1) All voltages values are measured with respect to the ground pin
- 2) The magnitude of input signal must never exceed V<sub>CC</sub> + 0.3V / GND - 0.3V
- 3) The voltage value is measured with respect from pin to supply

Table 3: Operating conditions

Symbol	Parameter	Value	Unit
V <sub>CC</sub>	Supply Voltage	2.2 to 5.5	V
V <sub>ICM</sub>	Common Mode Input Voltage Range	1.2V to V <sub>CC</sub>	V
V <sub>STB</sub>	Standby Voltage Input: Device ON Device OFF	1.35 ≤ V <sub>STB</sub> ≤ V <sub>CC</sub> GND ≤ V <sub>STB</sub> ≤ 0.4	V
R <sub>L</sub>	Load Resistor	≥ 4	Ω
R <sub>OUTGND</sub>	Resistor Output to GND (V <sub>STB</sub> = GND)	≥ 1	MΩ
T <sub>SD</sub>	Thermal Shutdown Temperature	150	°C
R <sub>THJA</sub>	Thermal Resistance Junction to Ambient QFN16 <sup>1</sup> QFN16 <sup>2</sup>	45 85	°C/W

- 1) When mounted on a 4-layer PCB with via
- 2) When mounted on a 2 layer PCB

### 3 Electrical characteristics

**Table 4: Electrical characteristics for  $V_{CC} = +5V$ ,  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)**

Symbol	Parameter	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply Current No input signal, no load		7.4	12	mA
$I_{STANDBY}$	Standby Current <sup>1</sup> No input signal, $V_{stdby} = G_{ND}$ , $R_L = 8\Omega$		10	1000	nA
$V_{OO}$	Output Offset Voltage No input signal, $R_L = 8\Omega$		1	10	mV
$P_{out}$	Output Power THD = 1% Max, $F = 1kHz$ , $R_L = 8\Omega$	0.8	1		W
THD + N	Total Harmonic Distortion + Noise $P_o = 1W_{rms}$ , $A_v = 2$ , $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.2		%
PSRR	Power Supply Rejection Ratio <sup>2</sup> $R_L = 8\Omega$ , $A_v = 2$ , $V_{ripple} = 200mV_{pp}$ , Input Grounded $F = 217Hz$ $F = 1kHz$	55 55	62 64		dB
Crosstalk	Channel Separation, $R_L = 8\Omega$ $F = 1kHz$ $F = 20Hz$ to $20kHz$		-92 -70		dB
$T_{WU}$	Wake-Up Time ( $C_b = 1\mu F$ )		90	130	ms
$T_{STDB}$	Standby Time ( $C_b = 1\mu F$ )		10		$\mu s$
$V_{STDBH}$	Standby Voltage Level High			1.3	V
$V_{STDBL}$	Standby Voltage Level Low			0.4	V
$\Phi_M$	Phase Margin at Unity Gain $R_L = 8\Omega$ , $C_L = 500pF$		65		Degrees
GM	Gain Margin $R_L = 8\Omega$ , $C_L = 500pF$		15		dB
GBP	Gain Bandwidth Product $R_L = 8\Omega$		1.5		MHz

1) Standby mode is activated when  $V_{stdby}$  is tied to  $Gnd$ .

2) All PSRR data limits are guaranteed by production sampling tests  
Dynamic measurements -  $20 \cdot \log(rms(V_{out})/rms(V_{ripple}))$ .  $V_{ripple}$  is the sinusoidal signal superimposed upon  $V_{cc}$ .

**Table 5: Electrical characteristics for  $V_{CC} = +3.3V$ ,  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)**

Symbol	Parameter	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply Current No input signal, no load		6.6	12	mA
$I_{STANDBY}$	Standby Current <sup>1</sup> No input signal, $V_{stdby} = G_{ND}$ , $R_L = 8\Omega$		10	1000	nA
$V_{OO}$	Output Offset Voltage No input signal, $R_L = 8\Omega$		1	10	mV
$P_{out}$	Output Power THD = 1% Max, $F = 1kHz$ , $R_L = 8\Omega$	300	450		mW
THD + N	Total Harmonic Distortion + Noise $P_o = 400mWrms$ , $A_v = 2$ , $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.1		%
PSRR	Power Supply Rejection Ratio <sup>2</sup> $R_L = 8\Omega$ , $A_v = 2$ , $V_{ripple} = 200mVpp$ , Input Grounded $F = 217Hz$ $F = 1kHz$	55 55	61 63		dB
Crosstalk	Channel Separation, $R_L = 8\Omega$ $F = 1kHz$ $F = 20Hz$ to $20kHz$		-94 -68		dB
$T_{WU}$	Wake-Up Time ( $C_b = 1\mu F$ )		110	140	ms
$T_{STDB}$	Standby Time ( $C_b = 1\mu F$ )		10		$\mu s$
$V_{STDBH}$	Standby Voltage Level High			1.2	V
$V_{STDBL}$	Standby Voltage Level Low			0.4	V
$\Phi_M$	Phase Margin at Unity Gain $R_L = 8\Omega$ , $C_L = 500pF$		65		Degrees
GM	Gain Margin $R_L = 8\Omega$ , $C_L = 500pF$		15		dB
GBP	Gain Bandwidth Product $R_L = 8\Omega$		1.5		MHz

1) Standby mode is activated when  $V_{stdby}$  is tied to  $Gnd$

2) All PSRR data limits are guaranteed by production sampling tests  
Dynamic measurements -  $20 \cdot \log(\text{rms}(V_{out})/\text{rms}(V_{ripple}))$ .  $V_{ripple}$  is the sinusoidal signal superimposed upon  $V_{cc}$ .

**Table 6: Electrical characteristics for  $V_{CC} = +2.6V$ ,  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)**

Symbol	Parameter	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply Current No input signal, no load		6.2	12	mA
$I_{STANDBY}$	Standby Current <sup>1</sup> No input signal, $V_{stdby} = G_{ND}$ , $R_L = 8\Omega$		10	1000	nA
$V_{OO}$	Output Offset Voltage No input signal, $R_L = 8\Omega$		1	10	mV
$P_{out}$	Output Power THD = 1% Max, $F = 1kHz$ , $R_L = 8\Omega$	200	250		mW
THD + N	Total Harmonic Distortion + Noise $P_o = 200mWrms$ , $A_v = 2$ , $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.1		%
PSRR	Power Supply Rejection Ratio <sup>2</sup> $R_L = 8\Omega$ , $A_v = 2$ , $V_{ripple} = 200mVpp$ , Input Grounded $F = 217Hz$ $F = 1kHz$	55 55	60 62		dB
Crosstalk	Channel Separation, $R_L = 8\Omega$ $F = 1kHz$ $F = 20Hz$ to $20kHz$		-95 -68		dB
$T_{WU}$	Wake-Up Time ( $C_b = 1\mu F$ )		125	150	ms
$T_{STDB}$	Standby Time ( $C_b = 1\mu F$ )		10		$\mu s$
$V_{STDBH}$	Standby Voltage Level High			1.2	V
$V_{STDBL}$	Standby Voltage Level Low			0.4	V
$\Phi_M$	Phase Margin at Unity Gain $R_L = 8\Omega$ , $C_L = 500pF$		65		Degrees
GM	Gain Margin $R_L = 8\Omega$ , $C_L = 500pF$		15		dB
GBP	Gain Bandwidth Product $R_L = 8\Omega$		1.5		MHz

1) Standby mode is activated when  $V_{stdby}$  is tied to  $Gnd$

2) All PSRR data limits are guaranteed by production sampling tests  
Dynamic measurements -  $20 \cdot \log(\text{rms}(V_{out})/\text{rms}(V_{ripple}))$ .  $V_{ripple}$  is the sinusoidal signal superimposed upon  $V_{cc}$ .

Figure 2: Open loop frequency response

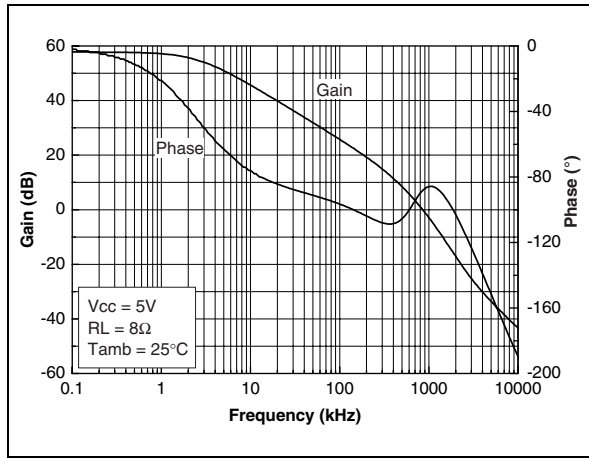


Figure 5: Open loop frequency response

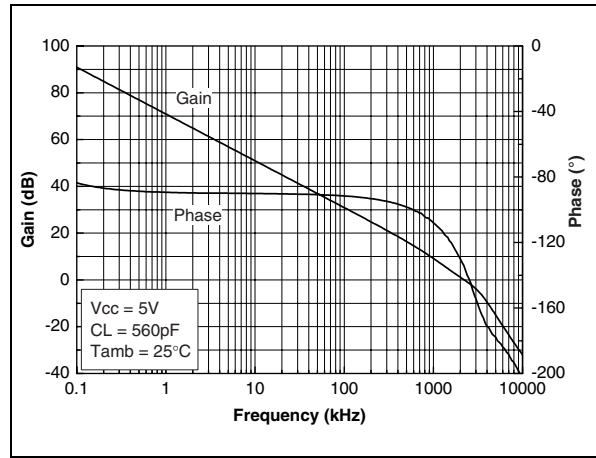


Figure 3: Open loop frequency response

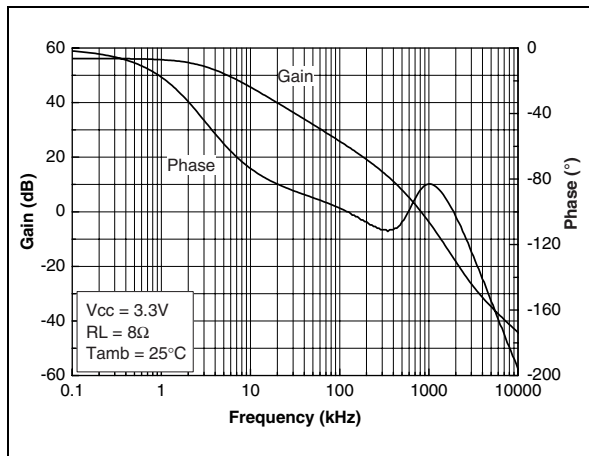


Figure 6: Open loop frequency response

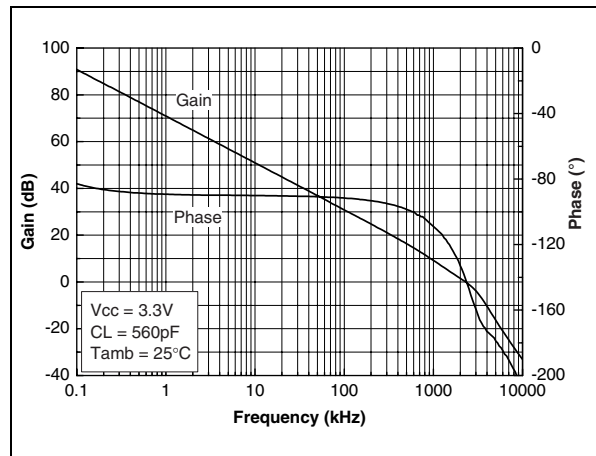


Figure 4: Open loop frequency response

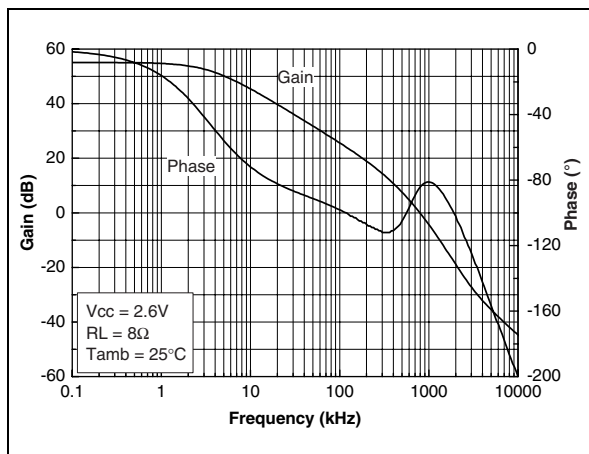


Figure 7: Open loop frequency response

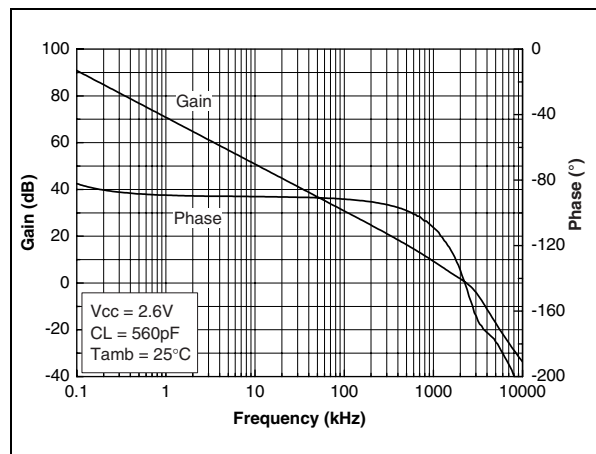


Figure 8: Power supply rejection ratio (PSRR) vs. frequency

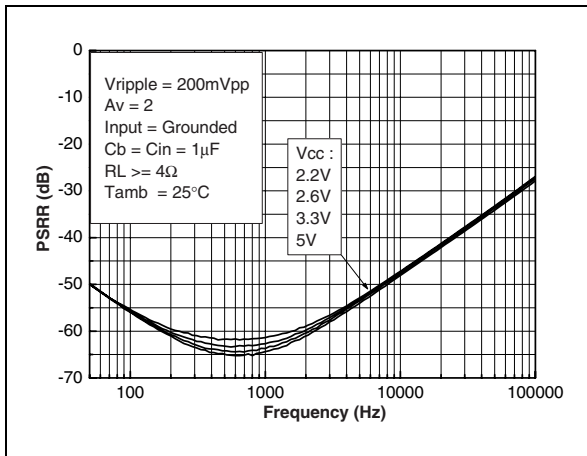


Figure 11: Power supply rejection ratio (PSRR) vs. frequency

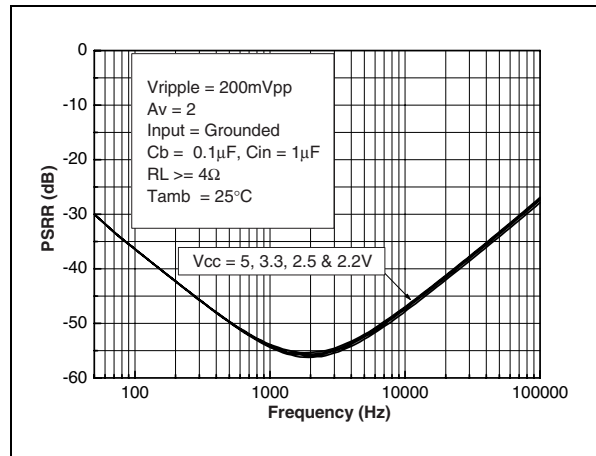


Figure 9: Power supply rejection ratio (PSRR) vs. frequency

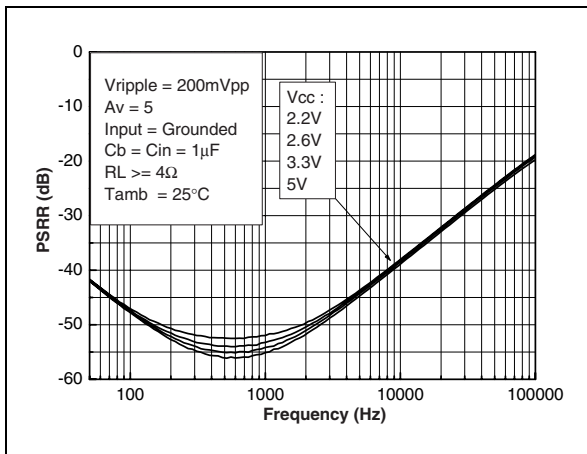


Figure 12: Power supply rejection ratio (PSRR) vs. frequency

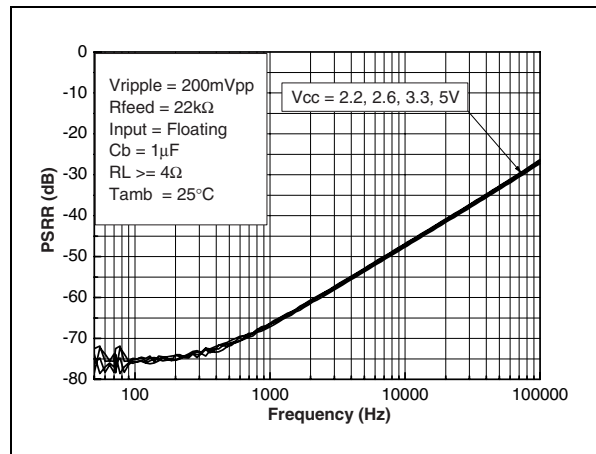


Figure 10: Power supply rejection ratio (PSRR) vs. frequency

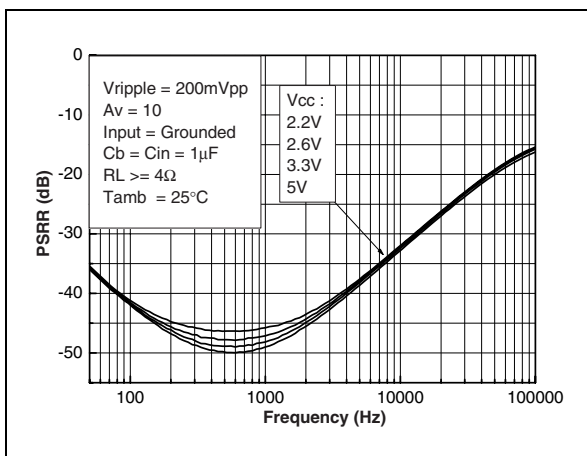


Figure 13: Power supply rejection ratio (PSRR) vs. frequency

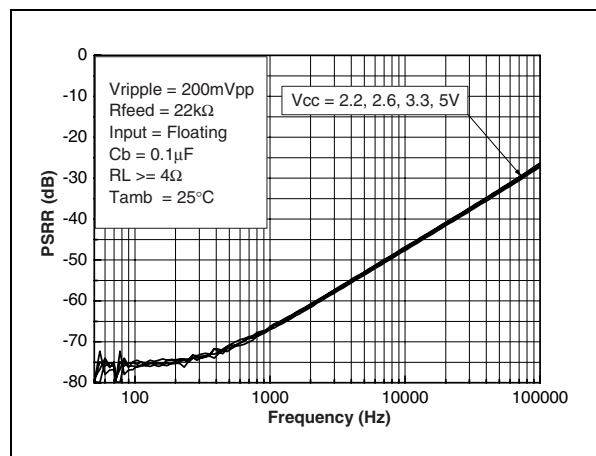




Figure 14: Power supply rejection ratio (PSRR) vs. DC output voltage

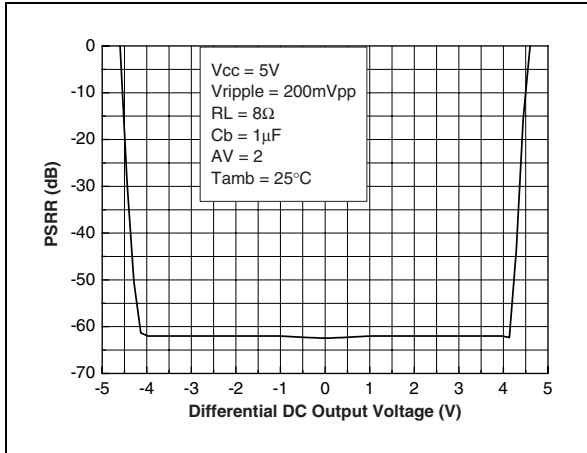


Figure 17: Power supply rejection ratio (PSRR) vs. DC output voltage

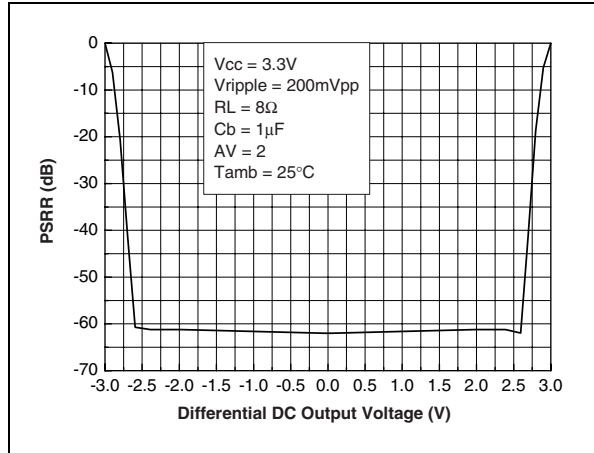


Figure 15: Power supply rejection ratio (PSRR) vs. DC output voltage

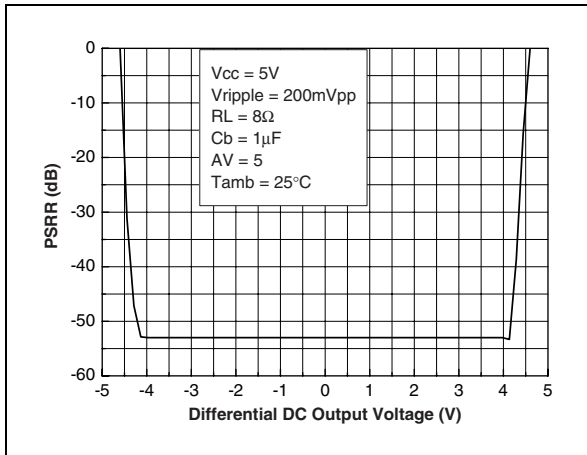


Figure 18: Power supply rejection ratio (PSRR) vs. DC output voltage

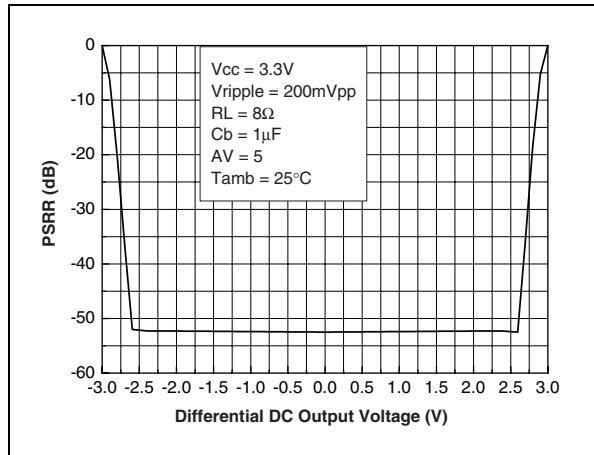


Figure 16: Power supply rejection ratio (PSRR) vs. DC output voltage

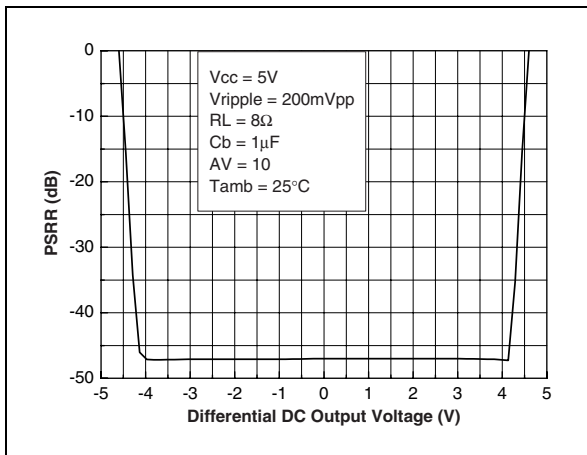


Figure 19: Power supply rejection ratio (PSRR) vs. DC output voltage

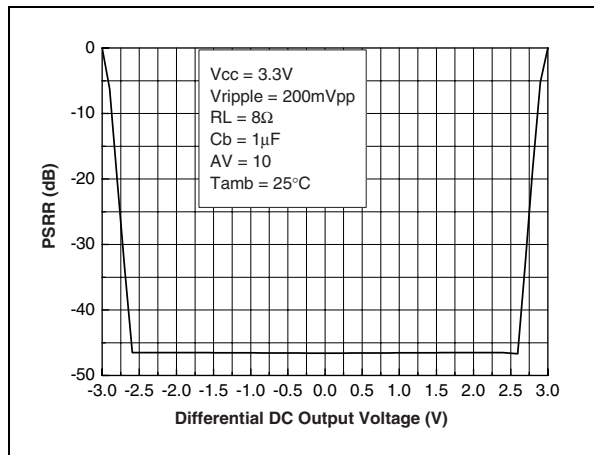


Figure 20: Power supply rejection ratio (PSRR) vs. DC output voltage

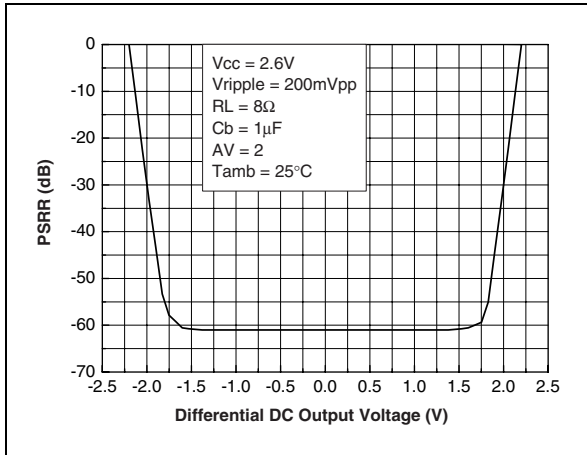


Figure 23: Power supply rejection ratio (PSRR) at f=217Hz vs. bypass capacitor

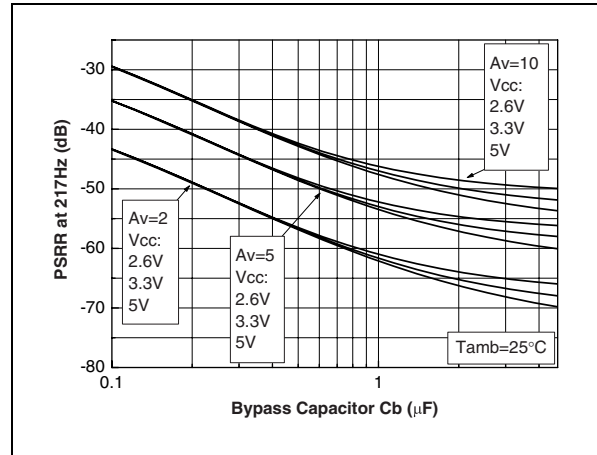


Figure 21: Power supply rejection ratio (PSRR) vs. DC output voltage

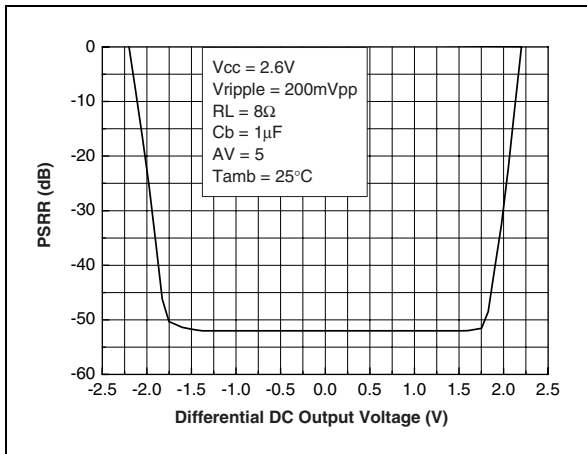


Figure 24: Output power vs. power supply voltage

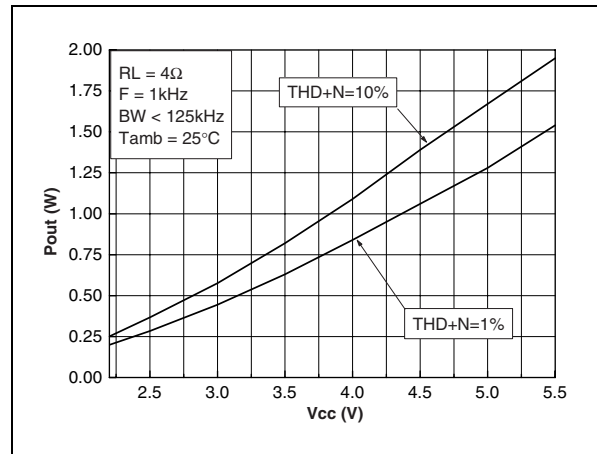


Figure 22: Power supply rejection ratio (PSRR) vs. DC output voltage

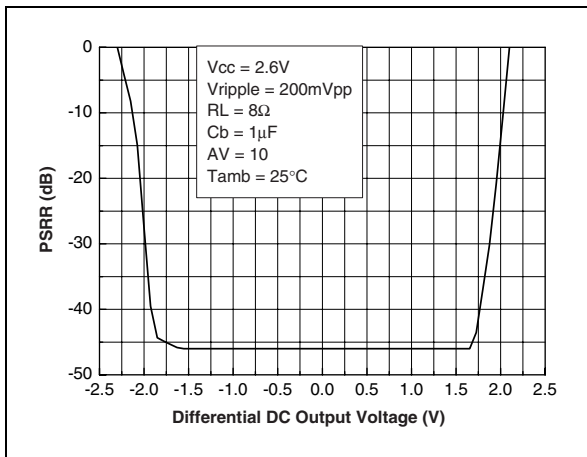


Figure 25: Output power vs. power supply voltage

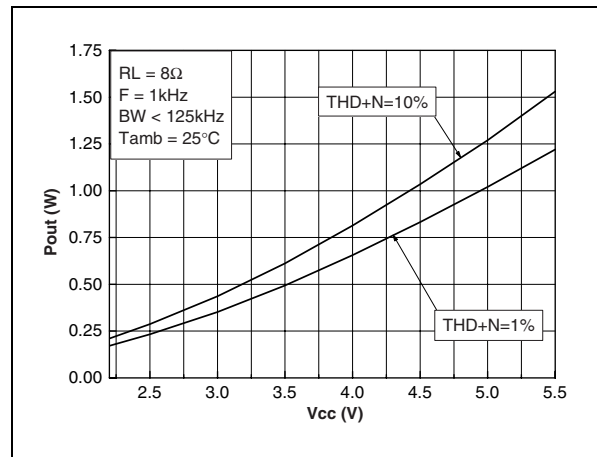


Figure 26: Output power vs. power supply voltage

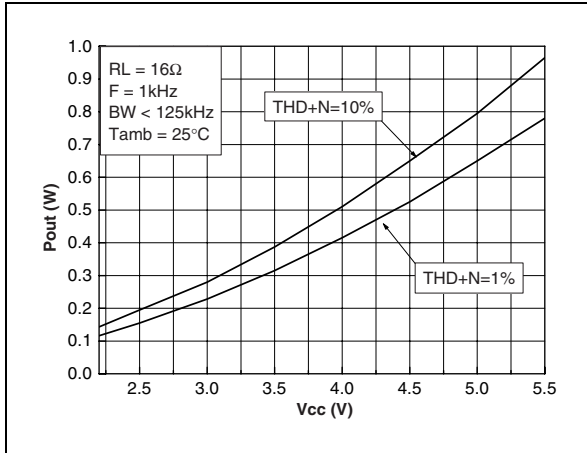


Figure 29: Output power vs. load resistor

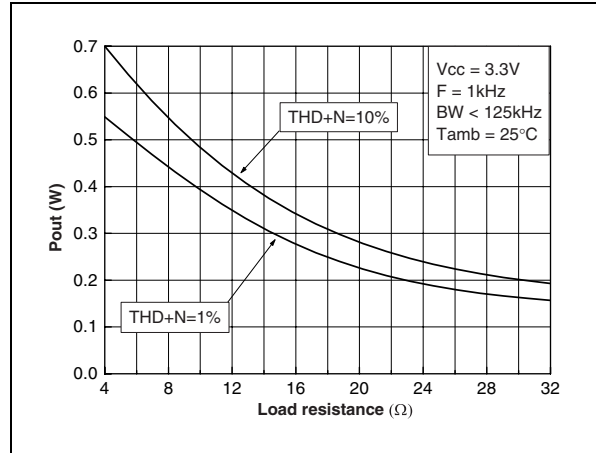


Figure 27: Output power vs. power supply voltage

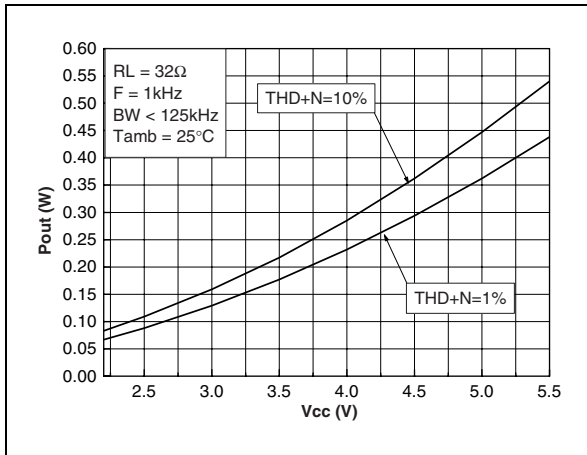


Figure 30: Output power vs. load resistor

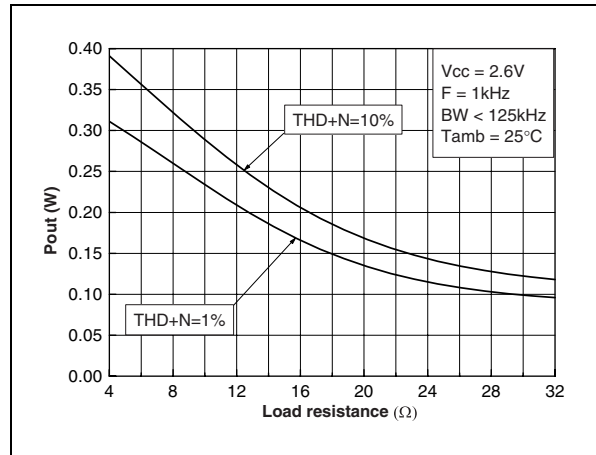


Figure 28: Output power vs. load resistor

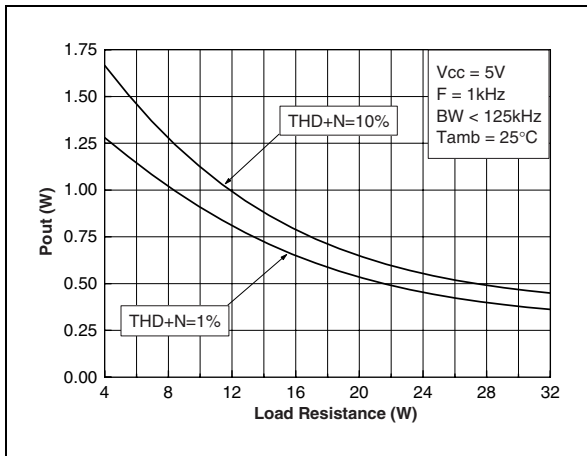


Figure 31: Power dissipation vs. output power

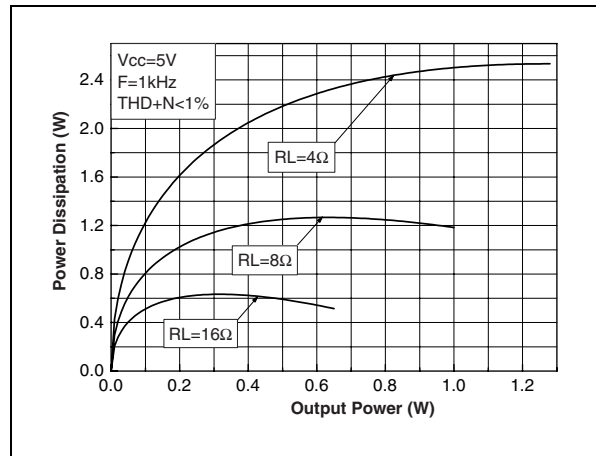


Figure 32: Power dissipation vs. output power

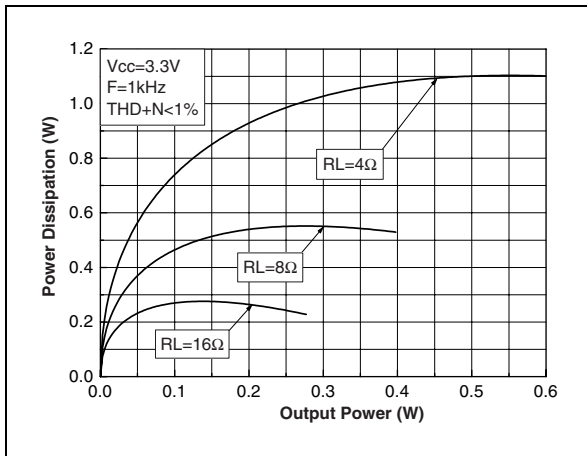


Figure 35: Clipping voltage vs. power supply voltage and load resistor

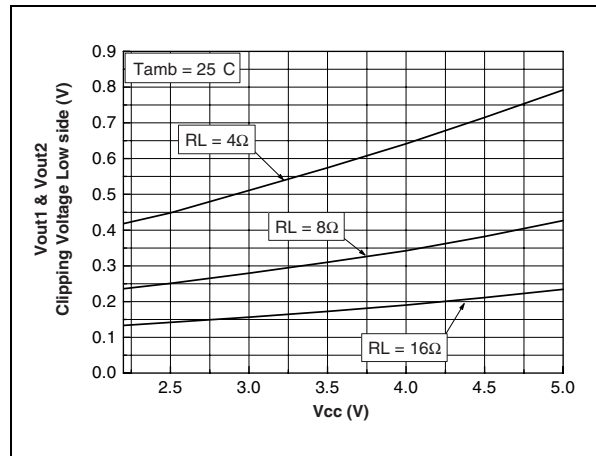


Figure 33: Power dissipation vs. output power

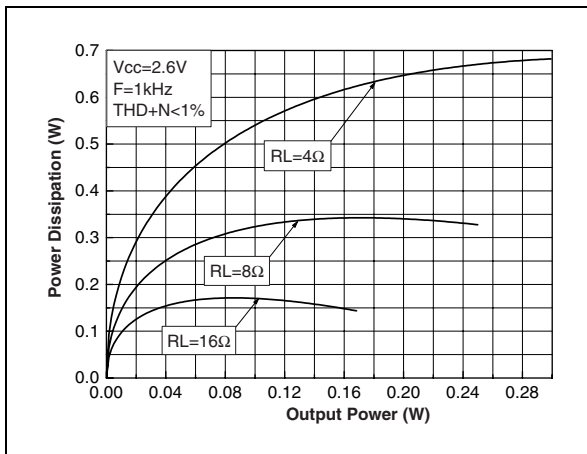


Figure 36: Current consumption vs. power supply voltage

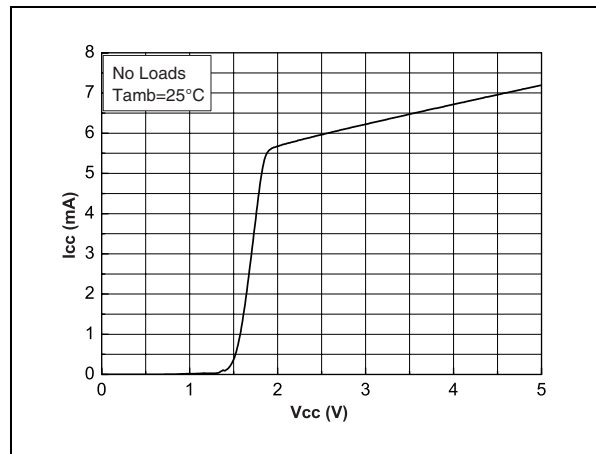


Figure 34: Clipping voltage vs. power supply voltage and load resistor

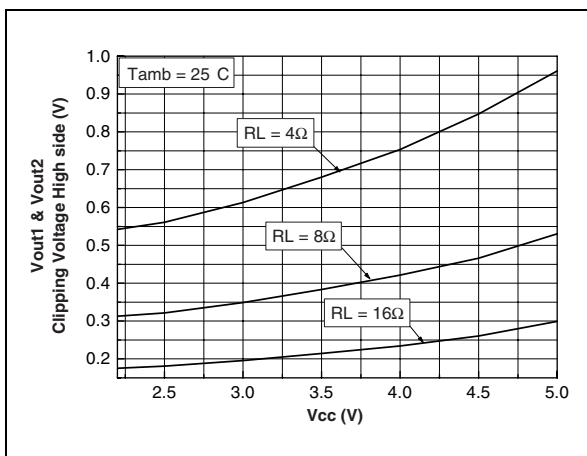


Figure 37: Current consumption vs. standby voltage at Vcc=5V

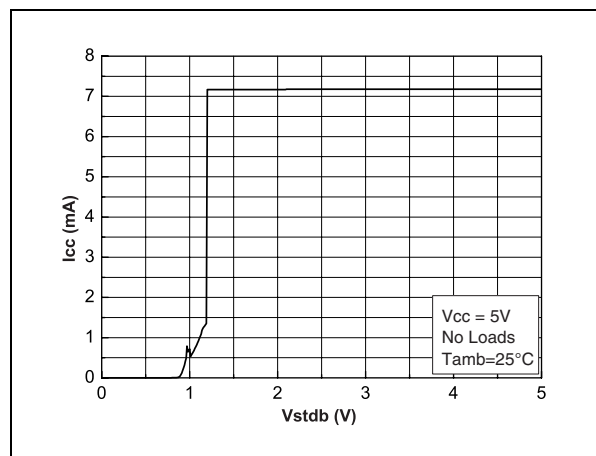


Figure 38: Current consumption vs. standby voltage at Vcc=3.3V

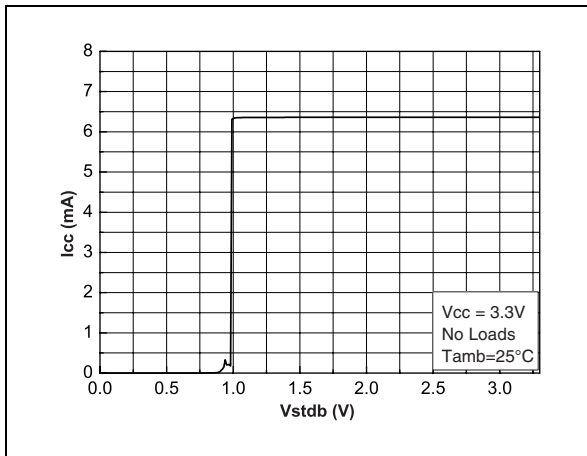


Figure 41: THD+N vs. output power

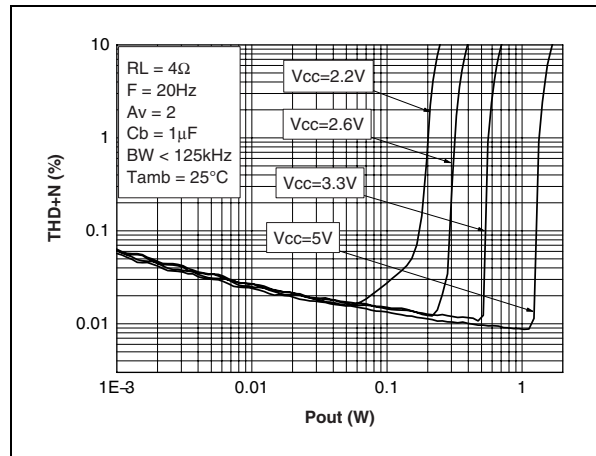


Figure 39: Current consumption vs. standby voltage at Vcc=2.6V

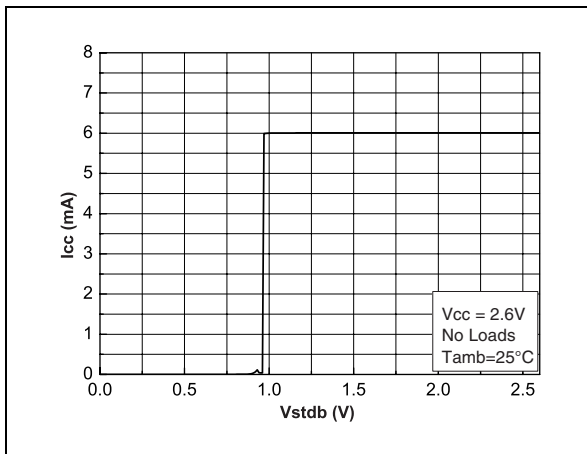


Figure 42: THD+N vs. output power

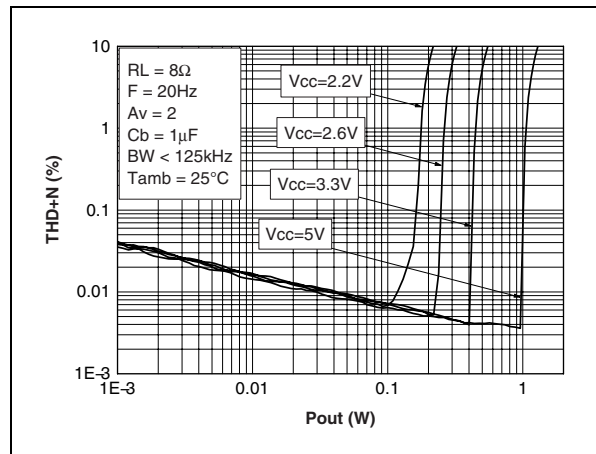


Figure 40: Current consumption vs. standby voltage at Vcc=2.2V

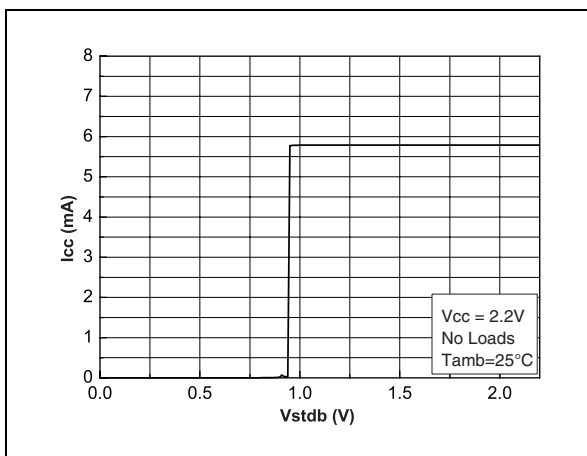


Figure 43: THD+N vs. output power

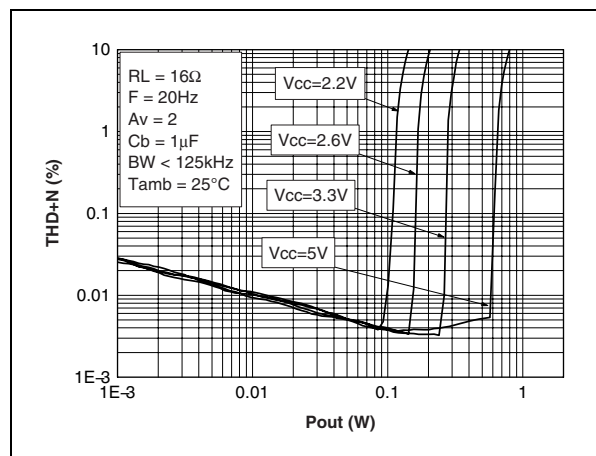


Figure 44: THD+N vs. output power

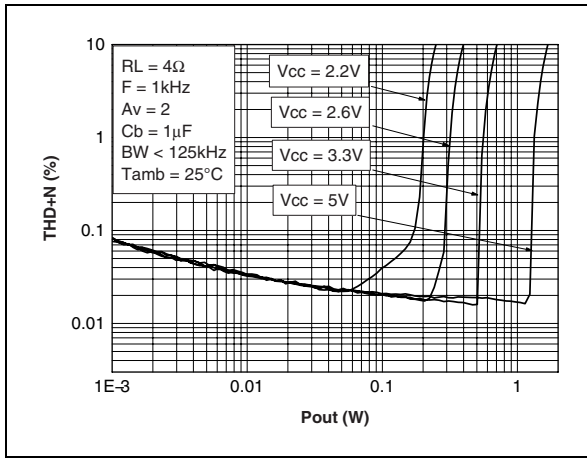


Figure 47: THD+N vs. output power

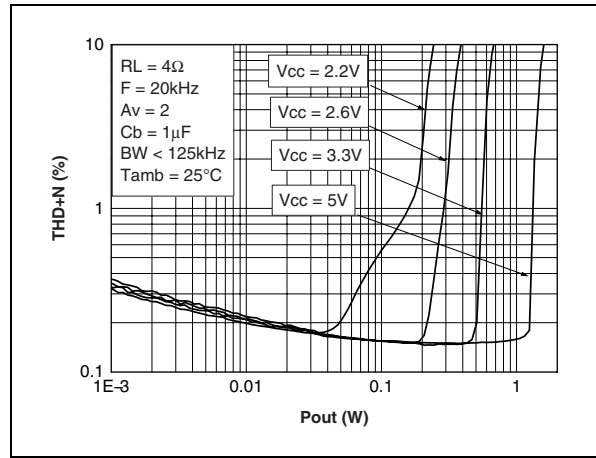


Figure 45: THD+N vs. output power

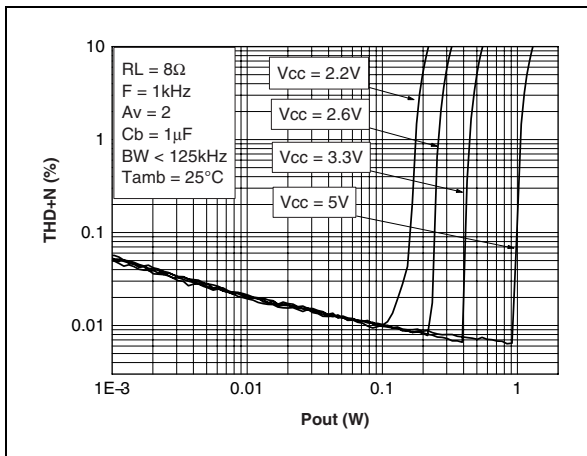


Figure 48: THD+N vs. output power

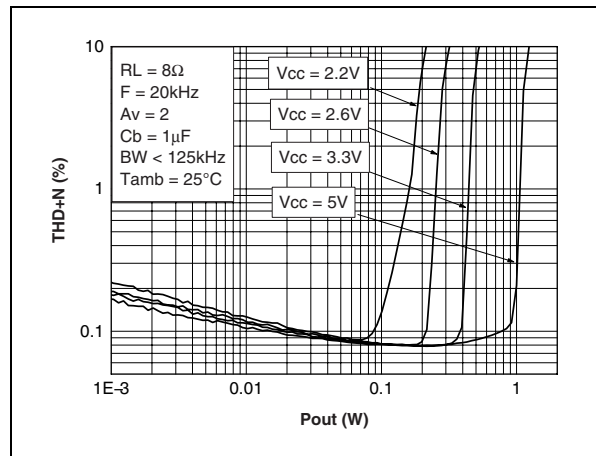


Figure 46: THD+N vs. output power

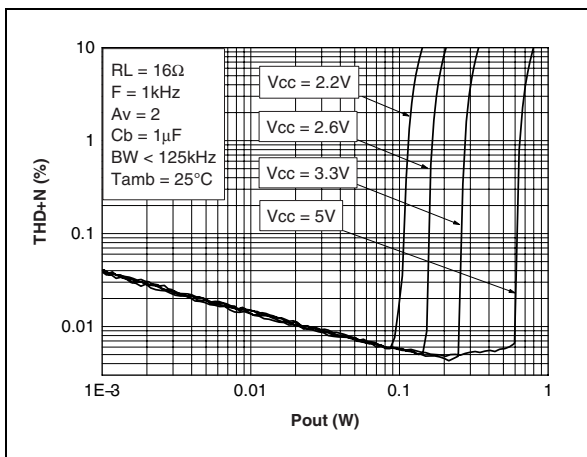


Figure 49: THD+N vs. output power

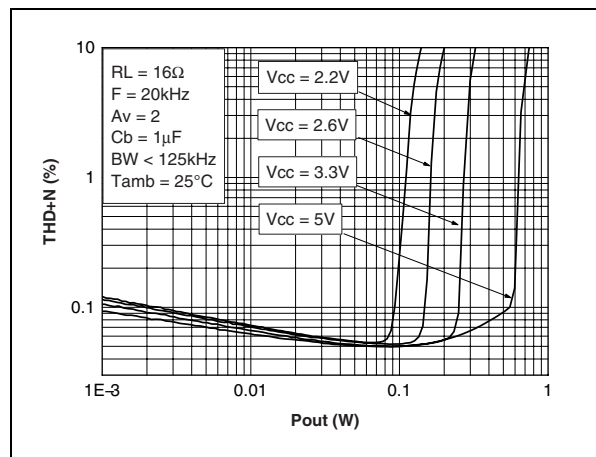


Figure 50: THD+N vs. frequency

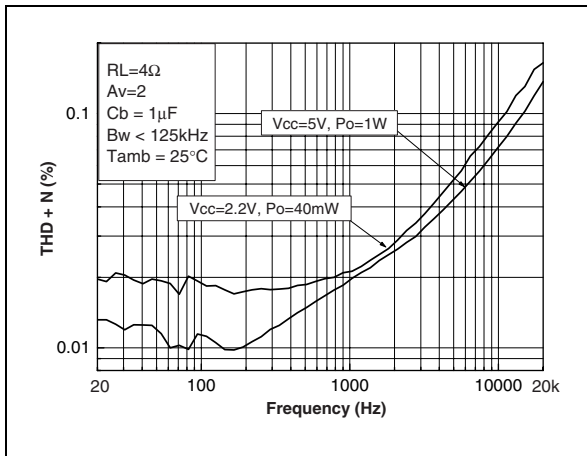


Figure 53: Signal to noise ratio vs. power supply with unweighted filter (20Hz to 20kHz)

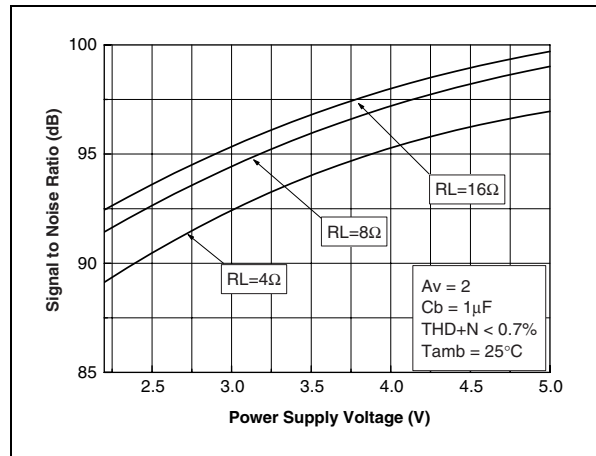


Figure 51: THD+N vs. frequency

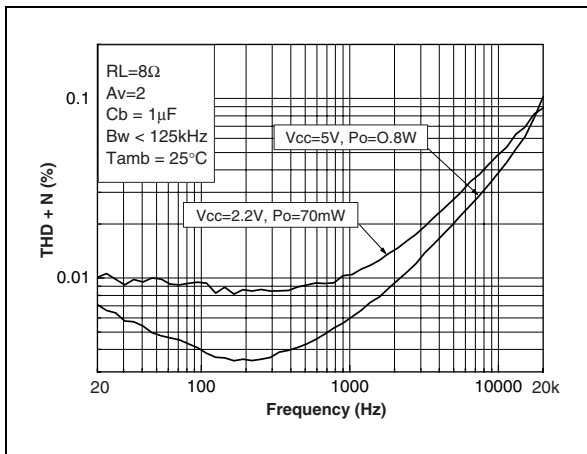


Figure 54: Signal to noise ratio vs. pwr supply with unweighted filter (20Hz to 20kHz)

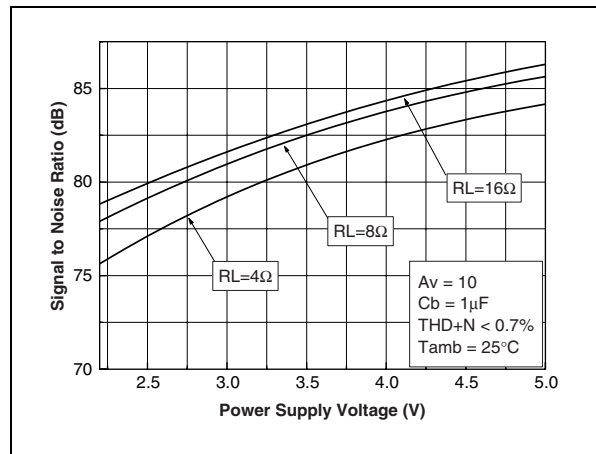


Figure 52: THD+N vs. frequency

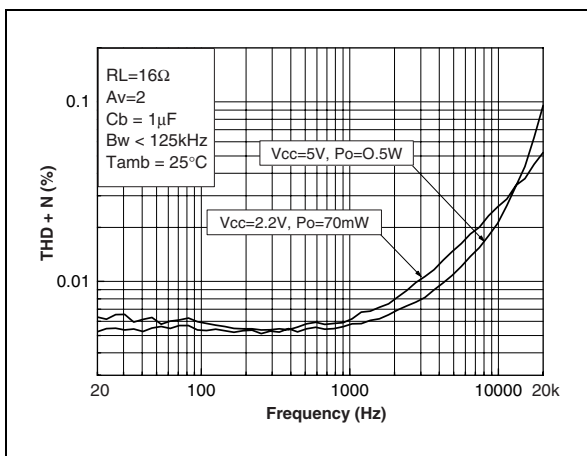


Figure 55: Signal to noise ratio vs. power supply with A weighted filter

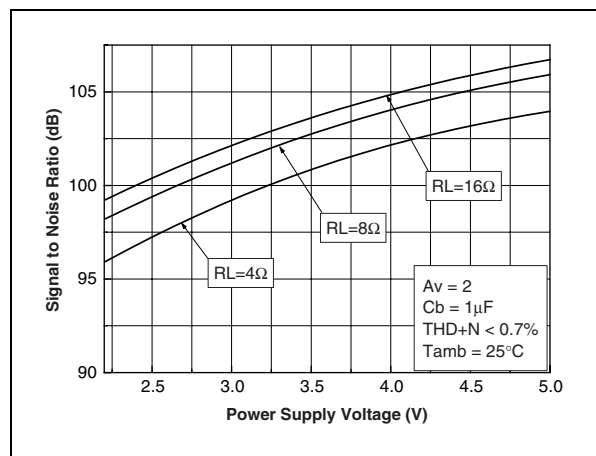


Figure 56: Signal to noise ratio vs. power supply with A weighted filter

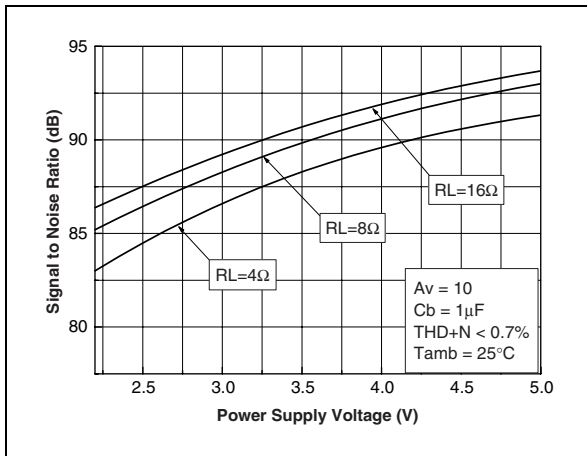


Figure 59: Crosstalk vs. frequency

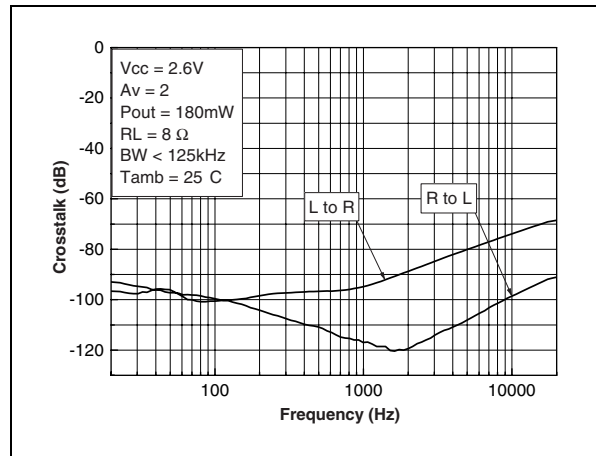


Figure 57: Crosstalk vs. frequency

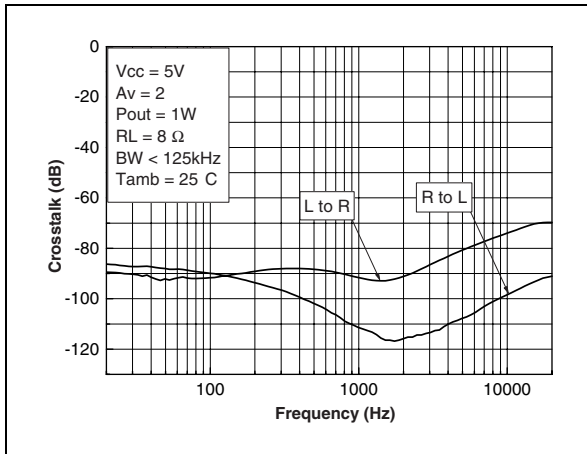


Figure 60: Crosstalk vs. frequency

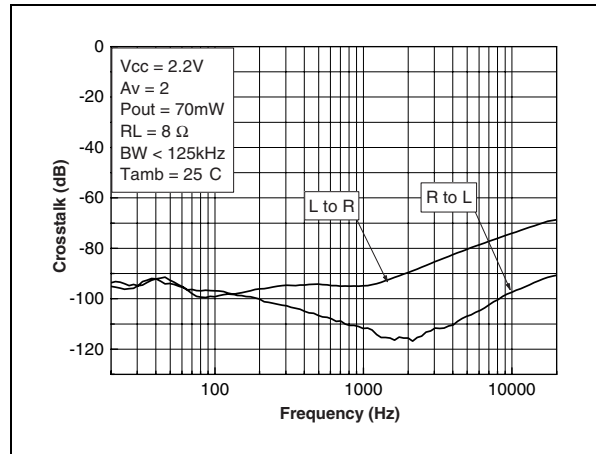


Figure 58: Crosstalk vs. frequency

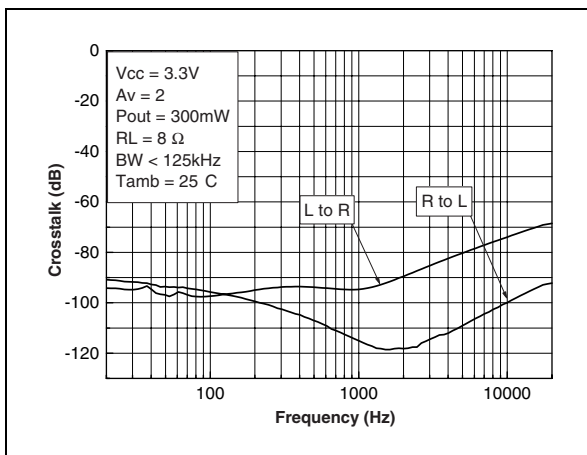


Figure 61: Output noise voltage, device ON

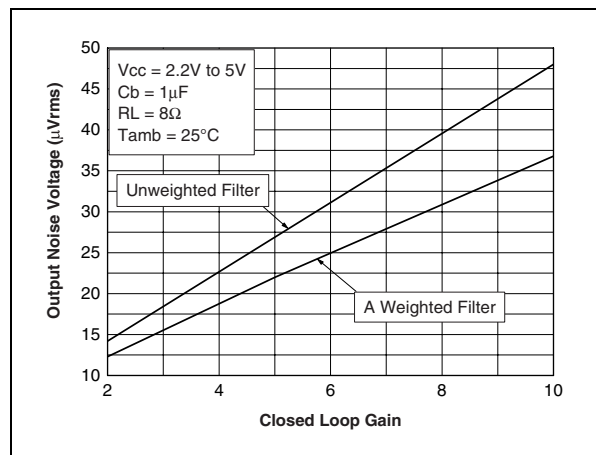




Figure 62: Output noise voltage, device in standby

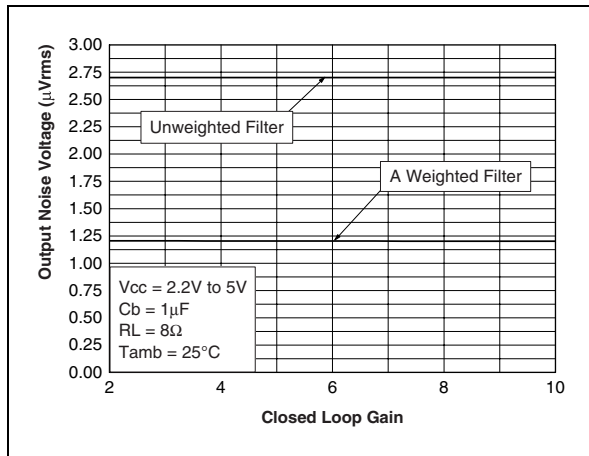
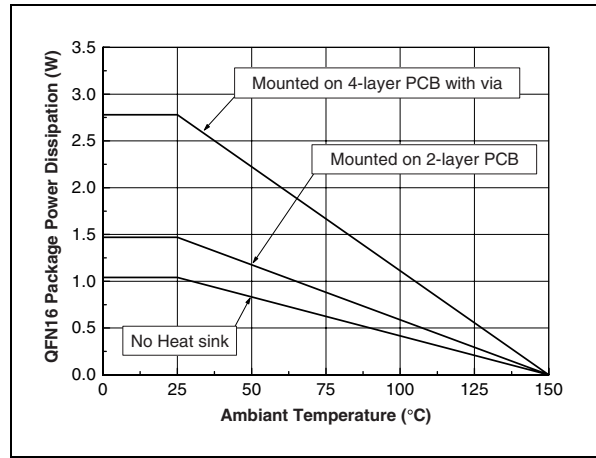


Figure 63: Power derating curves



### 4 Application Information

The TS4984 integrates two monolithic power amplifiers with a BTL (Bridge Tied Load) output type (explained in more detail in [Section 4.1](#)). For this discussion, only the left-channel amplifier will be referred to.

Referring to the schematic in [Figure 64](#), we assign the following variables and values:

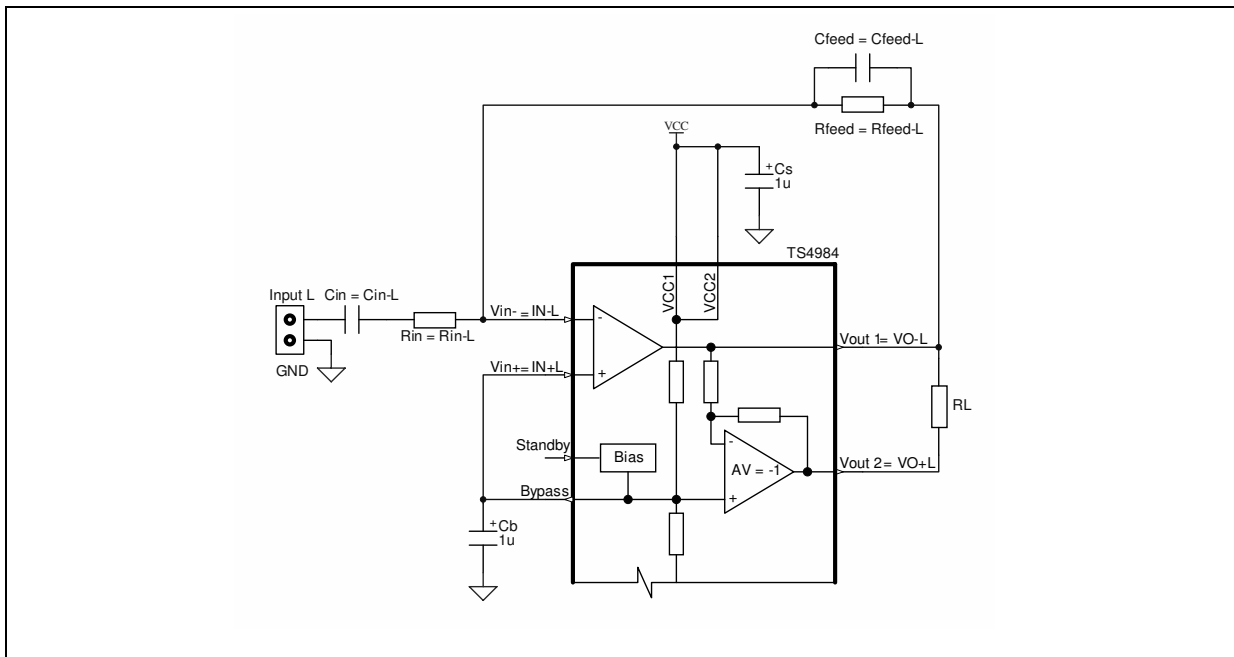
$$V_{in} = IN-L$$

$$V_{out1} = VO-L, V_{out2} = VO+R$$

$$R_{in} = Rin-L, R_{feed} = Rfeed-L$$

$$C_{feed} = Cfeed-L$$

**Figure 64: Typical application schematic - left channel**



#### 4.1 BTL configuration principle

BTL (Bridge Tied Load) means that each end of the load is connected to two single-ended output amplifiers. Thus, we have:

$$\text{Single-ended output 1} = V_{out1} = V_{out} \text{ (V)},$$

$$\text{Single-ended output 2} = V_{out2} = -V_{out} \text{ (V)}, V_{out1} - V_{out2} = 2V_{out} \text{ (V)}$$

The output power is:

$$P_{out} = \frac{(2V_{outRMS})^2}{R_L}$$

For the same power supply voltage, the output power in a BTL configuration is four times higher than the output power in a single-ended configuration.

#### 4.2 Gain in typical application schematic

The typical application schematic ([Figure 64](#)) is shown on [page 18](#).

In the flat region (no  $C_{in}$  effect), the output voltage of the first stage is:

$$V_{out1} = (-V_{in}) \frac{R_{feed}}{R_{in}} \quad (\text{V})$$

For the second stage:  $V_{out2} = -V_{out1}$  (V)

The differential output voltage is:

$$V_{out2} - V_{out1} = 2V_{in} \frac{R_{feed}}{R_{in}} \quad (\text{V})$$

The differential gain, referred to as  $G_V$  for greater convenience, is:

$$G_V = \frac{V_{out2} - V_{out1}}{V_{in}} = 2 \frac{R_{feed}}{R_{in}}$$

$V_{out2}$  is in phase with  $V_{in}$  and  $V_{out1}$  is phased  $180^\circ$  with  $V_{in}$ . This means that the positive terminal of the loudspeaker should be connected to  $V_{out2}$  and the negative to  $V_{out1}$ .

#### 4.3 Low and high frequency response

In the low frequency region,  $C_{in}$  starts to have an effect.  $C_{in}$  forms with  $R_{in}$  a high-pass filter with a -3dB cut-off frequency:

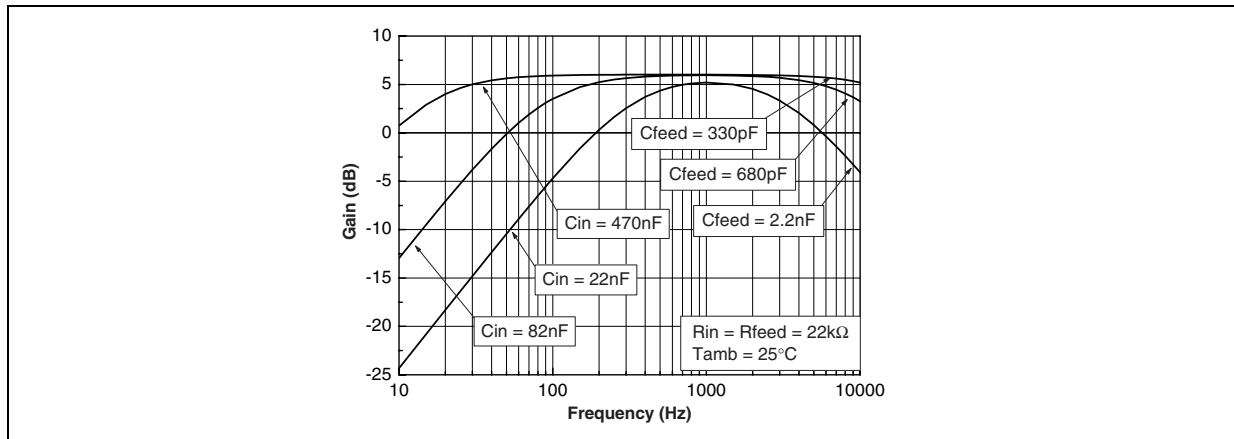
$$F_{CL} = \frac{1}{2\pi R_{in} C_{in}} \quad (\text{Hz})$$

In the high frequency region, you can limit the bandwidth by adding a capacitor ( $C_{feed}$ ) in parallel with  $R_{feed}$ . It forms a low-pass filter with a -3dB cut-off frequency.  $F_{CH}$  is in Hz.

$$F_{CH} = \frac{1}{2\pi R_{feed} C_{feed}} \quad (\text{Hz})$$

The following graph ([Figure 65](#)) shows an example of  $C_{in}$  and  $C_{feed}$  influence.

**Figure 65: Frequency response gain versus  $C_{in}$  &  $C_{feed}$**



#### 4.4 Power dissipation and efficiency

Hypotheses:

- Voltage and current in the load are sinusoidal ( $V_{out}$  and  $I_{out}$ ).
- Supply voltage is a pure DC source ( $V_{CC}$ ).

Regarding the load we have:

$$V_{out} = V_{PEAK} \sin \omega t \quad (V)$$

and

$$I_{out} = \frac{V_{out}}{R_L} \quad (A)$$

and

$$P_{out} = \frac{V_{PEAK}^2}{2R_L} \quad (W)$$

Therefore, the average current delivered by the supply voltage is:

$$I_{CC_{AVG}} = 2 \frac{V_{PEAK}}{\pi R_L} \quad (A)$$

The power delivered by the supply voltage is:

$$P_{supply} = V_{CC} \cdot I_{CC_{AVG}} \quad (W)$$

Then, the **power dissipated by each amplifier** is:

$$P_{diss} = P_{supply} - P_{out} \quad (W)$$

$$P_{diss} = \frac{2\sqrt{2}V_{CC}}{\pi\sqrt{R_L}} \cdot \sqrt{P_{out}} - P_{out} \quad (W)$$

and the maximum value is obtained when:

$$\frac{\partial P_{diss}}{\partial P_{out}} = 0$$

and its value is:

$$P_{dissmax} = \frac{2V_{CC}^2}{\pi^2 R_L} \quad (W)$$

*Note:* This maximum value is only depending on power supply voltage and load values.

The **efficiency**,  $\eta$ , is the ratio between the output power and the power supply:

$$\eta = \frac{P_{out}}{P_{supply}} = \frac{\pi V_{PEAK}}{4V_{CC}}$$

The maximum theoretical value is reached when  $V_{PEAK} = V_{CC}$ , so that:

$$\frac{\pi}{4} = 78.5\%$$

The TS4984 has two independent power amplifiers, and each amplifier produces heat due to its power dissipation. Therefore, the maximum die temperature is the sum of the each amplifier's maximum power dissipation. It is calculated as follows:

$P_{diss L}$  = Power dissipation due to the left channel power amplifier.

$P_{diss R}$  = Power dissipation due to the right channel power amplifier.

$$Total P_{diss} = P_{diss L} + P_{diss R} \quad (W)$$

In most cases,  $P_{diss L} = P_{diss R}$ , giving:

$$Total P_{diss} = 2P_{dissL} \quad (W)$$

or, stated differently:

$$Total P_{diss} = \frac{4\sqrt{2}V_{CC}}{\pi\sqrt{R_L}} \sqrt{P_{out}} - 2P_{out} \quad (W)$$

#### 4.5 Decoupling the circuit

Two capacitors are needed to correctly bypass the TS4984. A power supply bypass capacitor  $C_S$  and a bias voltage bypass capacitor  $C_B$ .

$C_S$  has particular influence on the THD+N in the high frequency region (above 7 kHz) and an indirect influence on power supply disturbances. With a value for  $C_S$  of 1  $\mu\text{F}$ , you can expect similar THD+N performances to those shown in the datasheet. For example:

- In the high frequency region, if  $C_S$  is lower than 1  $\mu\text{F}$ , it increases THD+N and disturbances on the power supply rail are less filtered.
- On the other hand, if  $C_S$  is higher than 1  $\mu\text{F}$ , those disturbances on the power supply rail are more filtered.

$C_B$  has an influence on THD+N at lower frequencies, but its function is critical to the final result of PSRR (with input grounded and in the lower frequency region), in the following manner:

- If  $C_B$  is lower than 1  $\mu\text{F}$ , THD+N increases at lower frequencies and PSRR worsens.
- If  $C_B$  is higher than 1  $\mu\text{F}$ , the benefit on THD+N at lower frequencies is small, but the benefit to PSRR is substantial.

Note that  $C_{in}$  has a non-negligible effect on PSRR at lower frequencies. The lower the value of  $C_{in}$ , the higher the PSRR.

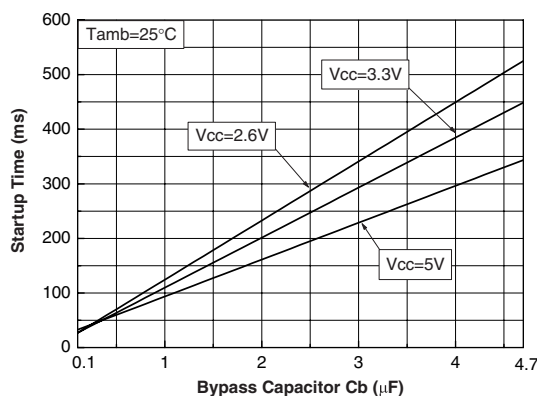
#### 4.6 Wake-up time, $T_{WU}$

When the standby is released to put the device ON, the bypass capacitor  $C_B$  will not be charged immediately. As  $C_B$  is directly linked to the bias of the amplifier, the bias will not work properly until the  $C_B$  voltage is correct. The time to reach this voltage is called wake-up time or  $T_{WU}$  and specified in electrical characteristics table with  $C_B = 1 \mu\text{F}$ .

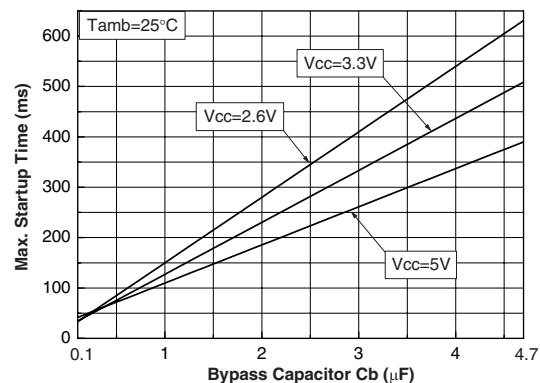
If  $C_B$  has a value other than 1  $\mu\text{F}$ , please refer to the graph in [Figure 66](#) to establish the wake-up time value.

Due to process tolerances, the maximum value of wake-up time could be established by the graph in [Figure 67](#).

**Figure 66: Typical wake-up time vs.  $C_B$**



**Figure 67: Maximum wake-up time vs.  $C_B$**



**Note:** Bypass capacitor  $C_B$  as also a tolerance of typically  $\pm 20\%$ . To calculate the wake-up time with this tolerance, refer to the previous graph (considering for example for  $C_B = 1 \mu\text{F}$  in the range of  $0.8 \mu\text{F} \leq 1 \mu\text{F} \leq 1.2 \mu\text{F}$ ).

#### 4.7 Shutdown time

When the standby command is set, the time required to put the two output stages in high impedance and the internal circuitry in shutdown mode is a few microseconds.

*Note:* In shutdown mode, Bypass pin and Vin- pin are short-circuited to ground by internal switches. This allows for the quick discharge of the  $C_b$  and  $C_{in}$  capacitors.

#### 4.8 Pop performance

Pop performance is intimately linked with the size of the input capacitor  $C_{in}$  and the bias voltage bypass capacitor  $C_b$ .

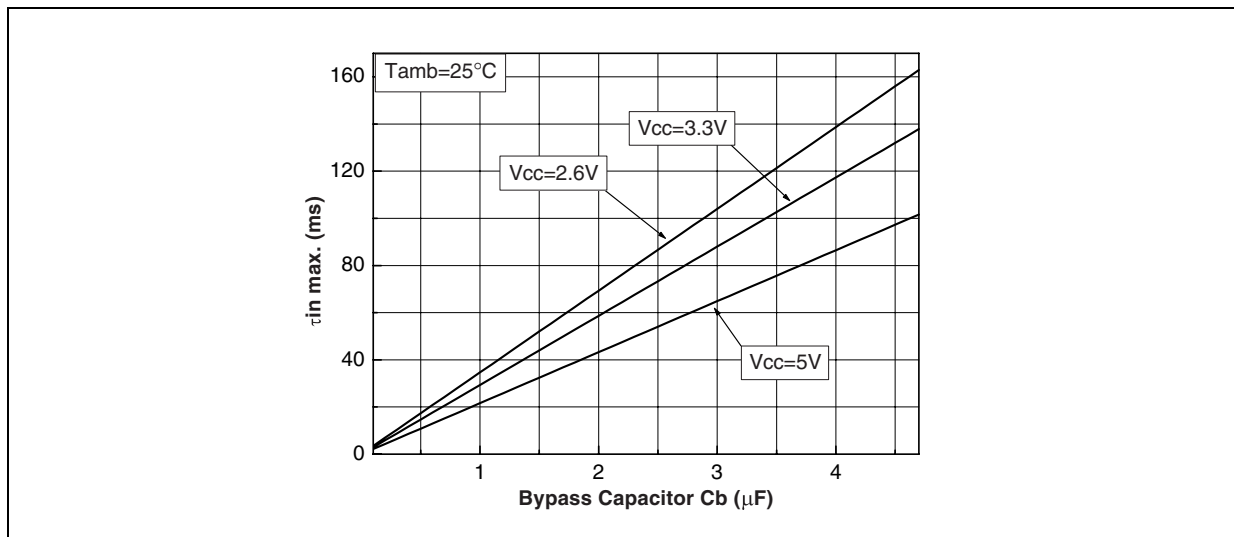
The size of  $C_{in}$  is dependent on the lower cut-off frequency and PSRR values requested. The size of  $C_b$  is dependent on THD+N and PSRR values requested at lower frequencies.

Moreover,  $C_b$  determines the speed with which the amplifier turns ON. In order to reach near zero pop and click, the equivalent input constant time is:

$$t_{in} = (R_{in} + 2 \text{ k}\Omega) \times C_{in} \text{ (s) with } R_{in} \geq 5 \text{ k}\Omega$$

must not reach the  $\tau_{in}$  maximum value as indicated in the graph below in [Figure 68](#).

**Figure 68:**  $\tau_{in}$  max. versus bypass capacitor



By following previous rules, the TS4984 can reach near zero pop and click even with high gains such as 20 dB.

#### Example calculation

With  $R_{in} = 22 \text{ k}\Omega$  and a 20 Hz, -3 dB low cut-off frequency,  $C_{in} = 361 \text{ nF}$ . So,  $C_{in} = 390 \text{ nF}$  with standard value which gives a lower cut-off frequency equal to 18.5 Hz. In this case,  $(R_{in} + 2 \text{ k}\Omega) \times C_{in} = 9.36 \text{ ms}$ . When referring to the previous graph, if  $C_b = 1 \mu\text{F}$  and  $V_{cc} = 5 \text{ V}$ , we read 20 ms max. This value is twice as high as our current value, thus we can state that pop and click will be reduced to its lowest value. Minimizing both  $C_{in}$  and the gain benefits both the pop phenomena, and the cost and size of the application.

4.9 Application example: Differential-input BTL power stereo amplifier

The schematic in *Figure 69* shows how to design the TS4984 to work in differential-input mode. For this discussion, only the left-channel amplifier will be referred to.

Let:

$$R_{1R} = R_{2L} = R_1, R_{2R} = R_{2L} = R_2$$

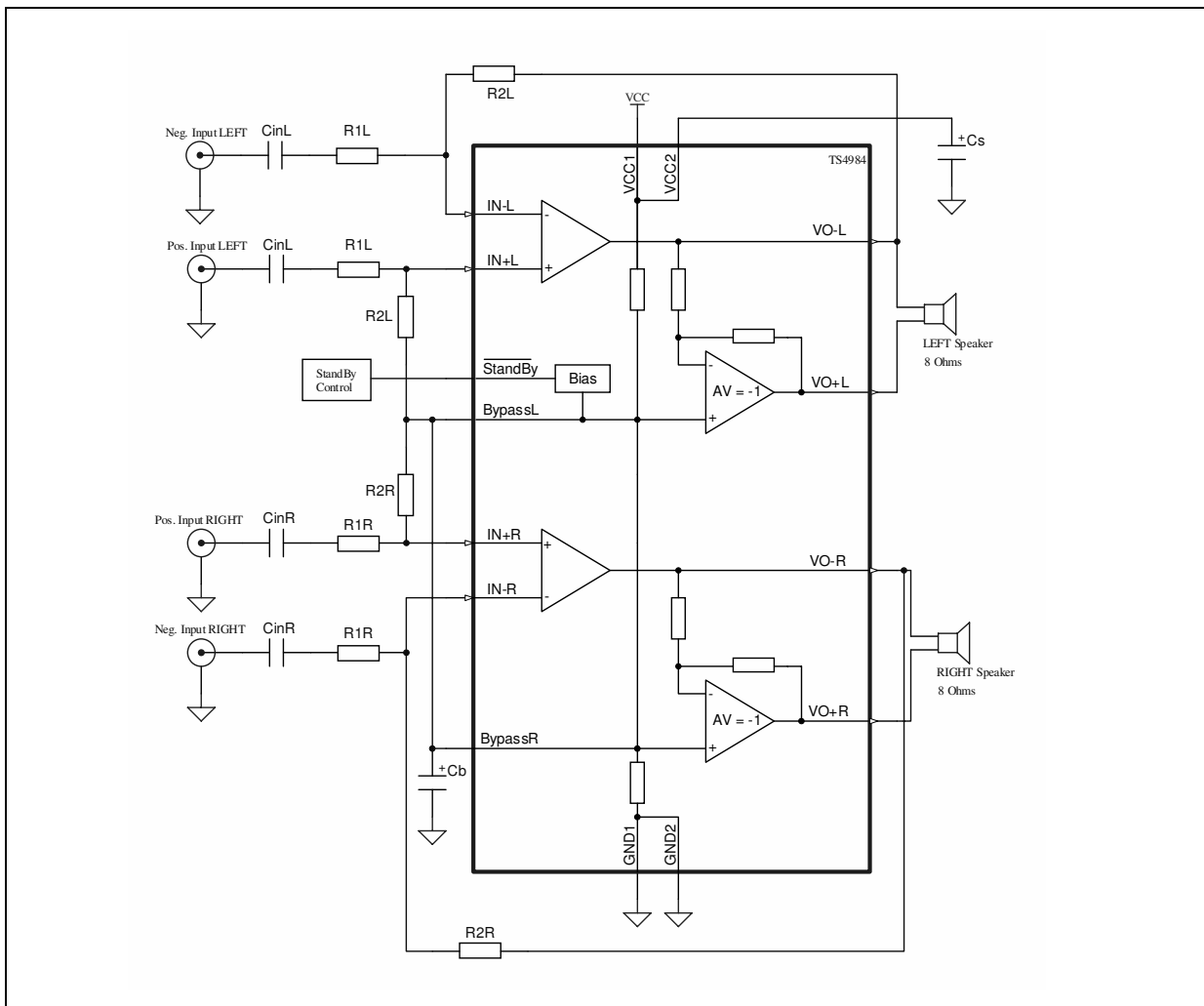
$$C_{inR} = C_{inL} = C_{in}$$

The gain of the amplifier is:

$$G_{vdif} = 2 \times \frac{R_2}{R_1}$$

In order to reach the optimal performance of the differential function,  $R_1$  and  $R_2$  should be matched at 1% maximum.

Figure 69: Differential input amplifier configuration





The value of the input capacitor  $C_{IN}$  can be calculated with the following formula, using the -3dB lower frequency required (where  $F_L$  is the lower frequency required):

$$C_{IN} \approx \frac{1}{2 \pi R_1 F_L} \text{ (F)}$$

*Note: This formula is true only if:*

$$F_{CB} = \frac{1}{2 \pi (R_1 + R_2) C_B} \text{ (Hz)}$$

*is 5 times lower than  $F_L$ .*

The following bill of materials is provided as an example of a differential amplifier with a gain of 2 and a -3 dB lower cut-off frequency of about 80 Hz.

**Table 7: Example of a bill of material**

Designator	Part Type
$R_{1L} = R_{1R}$	20kΩ / 1%
$R_{2L} = R_{2R}$	20kΩ / 1%
$C_{inR} = C_{inL}$	100nF
$C_b = C_s$	1μF
U1	TS4984

### 4.10 Demoboard

A demoboard for the TS4984 is available.

For more information about this demoboard, please refer to **Application Note AN2049**, which can be found on [www.st.com](http://www.st.com).

*Figure 70* shows the schematic of the demoboard. *Figure 71*, *Figure 72* and *Figure 73* show the component locations, top layer and bottom layer respectively.

**Figure 70: Demoboard schematic**

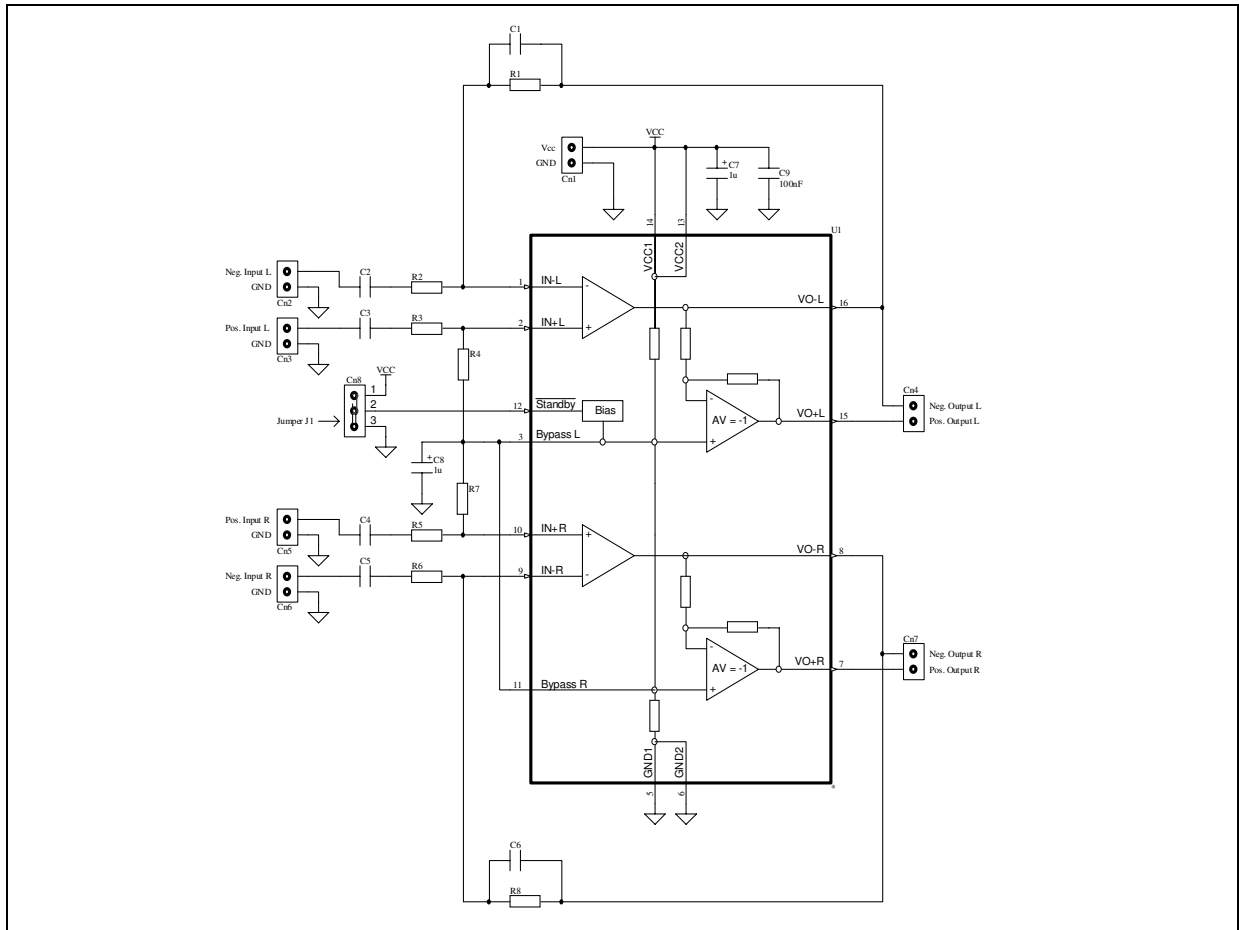


Figure 71: Components location

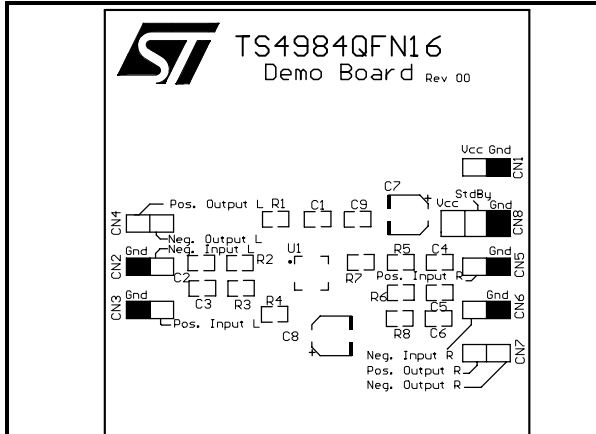


Figure 72: Top layer

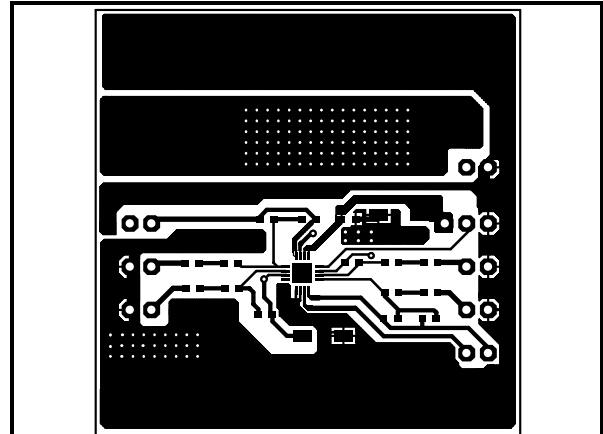
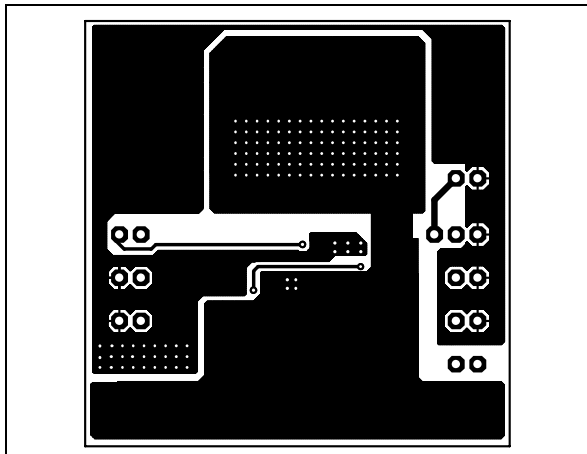
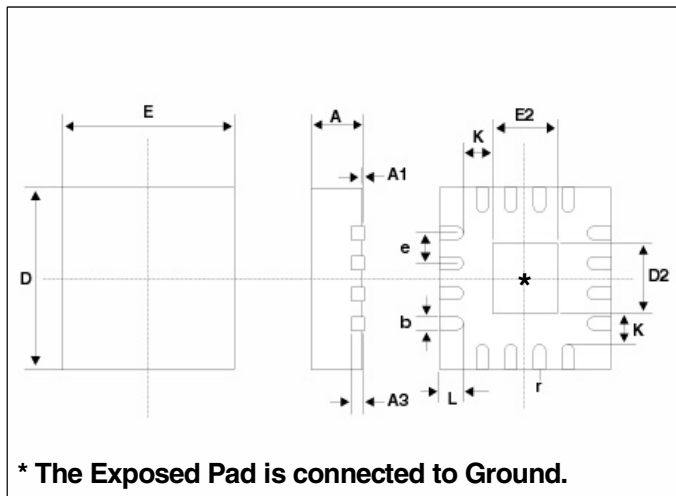


Figure 73: Bottom layer



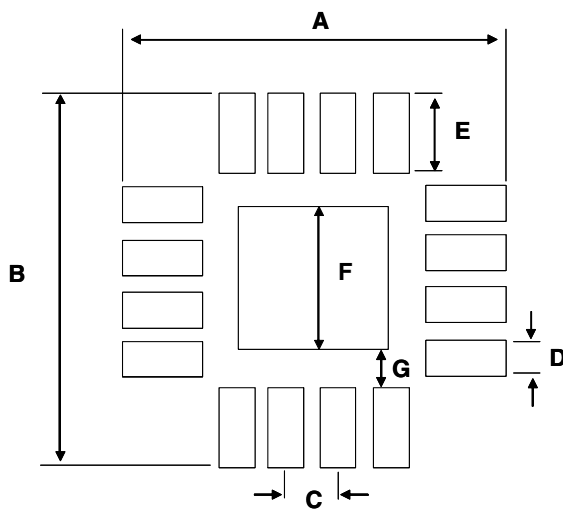
5 Package Mechanical Data

5.1 Dimensions of QFN16 package



DIMENSIONS			
REF	mm		
	MIN.	TYP.	MAX.
A	0.8	0.9	1.0
A1		0.02	0.05
A3		0.20	
b	0.18	0.25	0.30
D	3.85	4.0	4.15
D2	2.1		2.6
E	3.85	4.0	4.15
E2	2.1		2.6
e		0.50	
K	0.2		
L	0.30	0.40	0.50
r	0.11		

5.2 Footprint recommended data



FOOTPRINT DATA	
	mm
A	5.0
B	5.0
C	0.5
D	0.35
E	0.45
F	2.70
G	0.22

## 6 Revision History

Date	Revision	Description of Changes
01 Jan 2005	1	First Release

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