

## 1.2 W fully differential audio power amplifier with selectable standby and 6 dB fixed gain

### Features

- Differential inputs
- 90 dB PSRR @ 217 Hz with grounded inputs
- Operates from  $V_{CC} = 2.5\text{ V}$  to  $5.5\text{ V}$
- 1.2 W rail-to-rail output power @  $V_{CC}=5\text{ V}$ , THD+N=1%, F=1 kHz, with an  $8\ \Omega$  load
- 6 dB integrated fixed gain
- Ultra-low consumption in standby mode (10 nA)
- Selectable standby mode (active low or active high)
- Ultra-fast startup time: 10 ms typ. at  $V_{CC}=3.3\text{ V}$
- Available in 9-bump flip chip (300 mm bump diameter)
- Ultra-low pop and click

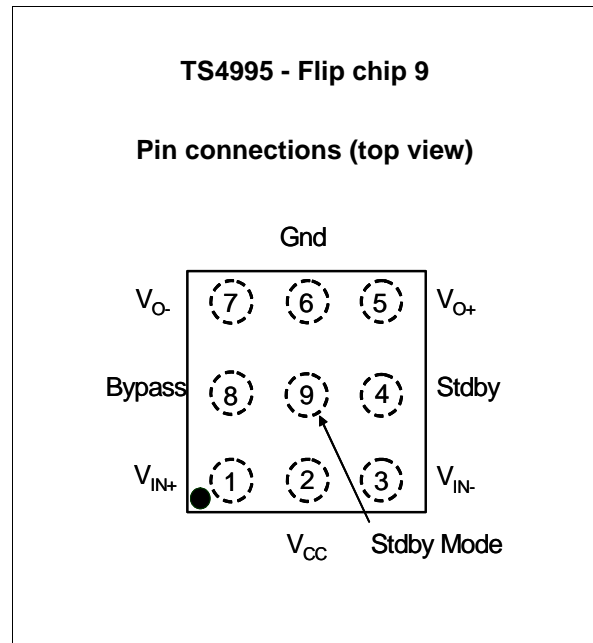
### Applications

- Mobile phones (cellular / cordless)
- PDAs
- Laptop / notebook computers
- Portable audio devices

### Description

The TS4995 is an audio power amplifier capable of delivering 1.2 W of continuous RMS output power into an  $8\ \Omega$  load at 5 V. Thanks to its differential inputs, it exhibits outstanding noise immunity.

An external standby mode control reduces the supply current to less than 10 nA. A STBY MODE pin allows the standby pin to be active **high** or **low**. An internal thermal shutdown protection is also provided, making the device capable of sustaining short-circuits.



The TS4995 features an internal fixed gain at 6dB which reduces the number of external components on the application board.

The device is equipped with common mode feedback circuitry allowing outputs to be always biased at  $V_{CC}/2$  regardless of the input common mode voltage.

The TS4995 is specifically designed for high quality audio applications such as mobile phones and requires few external components.

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# 1 Absolute maximum ratings and operating conditions

**Table 1. Absolute maximum ratings (AMR)**

Symbol	Parameter	Value	Unit
$V_{CC}$	Supply voltage <sup>(1)</sup>	6	V
$V_{in}$	Input voltage <sup>(2)</sup>	GND to $V_{CC}$	V
$T_{oper}$	Operating free air temperature range	-40 to + 85	°C
$T_{stg}$	Storage temperature	-65 to +150	°C
$T_j$	Maximum junction temperature	150	°C
$R_{thja}$	Thermal resistance junction to ambient <sup>(3)</sup>	200	°C/W
$P_{diss}$	Power dissipation	Internally limited	W
ESD	MM: machine model <sup>(4)</sup>	200	V
	HBM: human body model <sup>(5)</sup>	1.5	kV
Latch-up	Latch-up immunity	200	mA
-	Lead temperature (soldering, 10sec)	260	°C

- All voltage values are measured with respect to the ground pin.
- The magnitude of input signal must never exceed  $V_{CC} + 0.3\text{ V} / \text{GND} - 0.3\text{ V}$ .
- The device is protected in case of over temperature by a thermal shutdown activated at 150° C.
- Machine model: a 200 pF cap is charged to the specified voltage, then discharged directly between two pins of the device with no external series resistor (internal resistor < 5  $\Omega$ ), done for all couples of pin combinations with other pins floating.
- Human body model: 100 pF discharged through a 1.5 k $\Omega$  resistor between two pins of the device, done for all couples of pin combinations with other pins floating.

**Table 2. Operating conditions**

Symbol	Parameter	Value	Unit
$V_{CC}$	Supply voltage	2.5 to 5.5	V
$V_{SM}$	Standby mode voltage input:	$V_{SM}=\text{GND}$ $V_{SM}=V_{CC}$	V
	Standby Active LOW Standby Active HIGH		
$V_{STBY}$	Standby voltage input:	$1.5 \leq V_{STBY} \leq V_{CC}$ $\text{GND} \leq V_{STBY} \leq 0.4$ <sup>(1)</sup>	V
	Device ON ( $V_{SM}=\text{GND}$ ) or Device OFF ( $V_{SM}=V_{CC}$ ) Device OFF ( $V_{SM}=\text{GND}$ ) or Device ON ( $V_{SM}=V_{CC}$ )		
$T_{SD}$	Thermal shutdown temperature	150	°C
$R_L$	Load resistor	$\geq 4$	$\Omega$
$R_{thja}$	Thermal resistance junction to ambient	100	°C/W

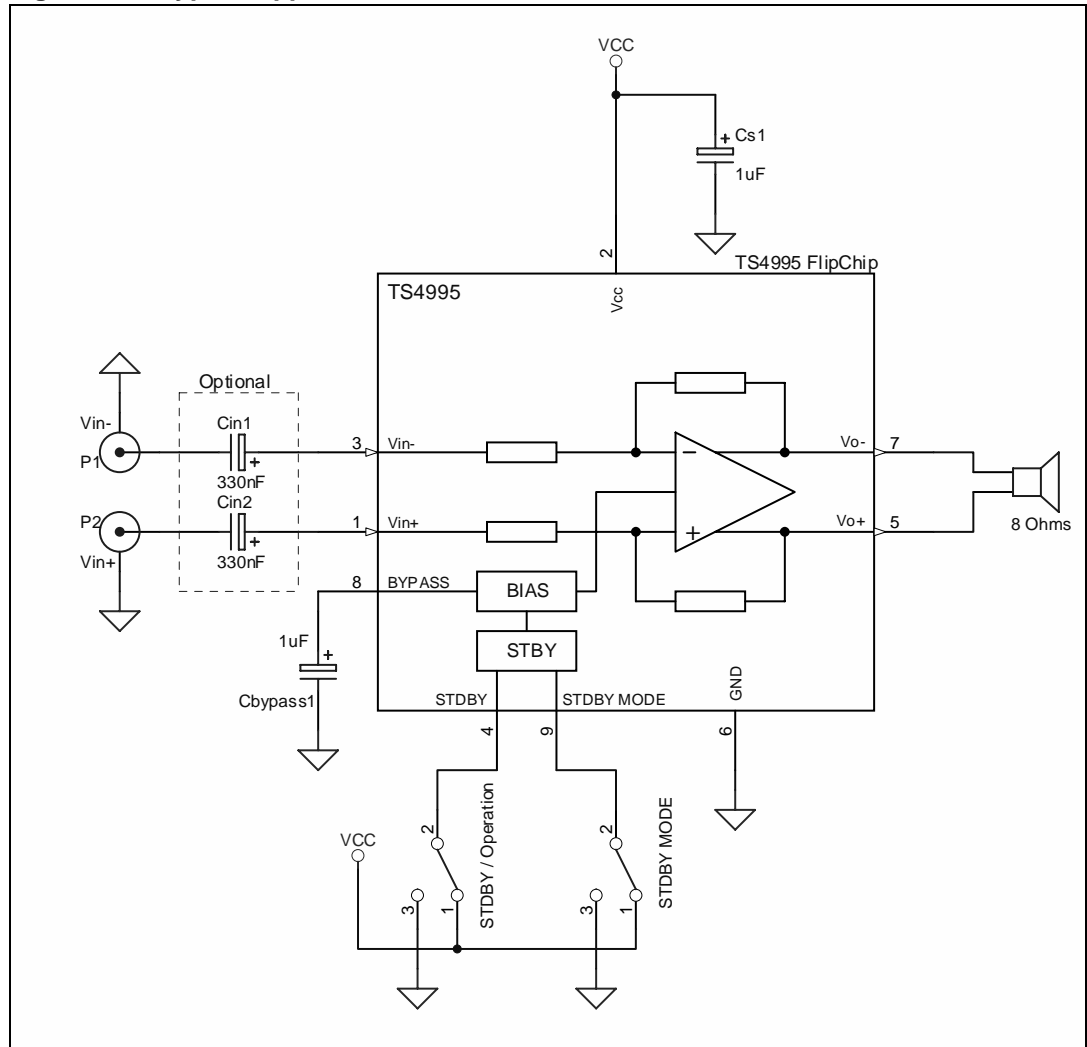
- The minimum current consumption ( $I_{STBY}$ ) is guaranteed when  $V_{STBY} = \text{GND}$  or  $V_{CC}$  (the supply rails) for the whole temperature range.

## 2 Typical application schematics

**Table 3. External component descriptions**

Component	Functional description
C <sub>s</sub>	Supply bypass capacitor that provides power supply filtering.
C <sub>b</sub>	Bypass capacitor that provides half supply filtering.
C <sub>in</sub>	Optional input capacitor that forms a high pass filter together with R <sub>in</sub> . ( $F_{cl} = 1 / (2 \times \pi \times R_{in} \times C_{in})$ )

**Figure 1. Typical application**



### 3 Electrical characteristics

Table 4.  $V_{CC} = +5V$ ,  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)

Symbol	Parameter	Test conditions	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply current	No input signal, no load		4	7	mA
$I_{STBY}$	Standby current	No input signal, $V_{STBY} = V_{SM} = GND$ , $R_L = 8\Omega$ No input signal, $V_{STBY} = V_{SM} = V_{CC}$ , $R_L = 8\Omega$		10	1000	nA
$V_{oo}$	Differential output offset voltage	No input signal, $R_L = 8\Omega$		0.1	10	mV
$V_{IC}$	Input common mode voltage		0		4.5	V
$P_o$	Output power	THD = 1% Max, $F = 1kHz$ , $R_L = 8\Omega$	0.8	1.2		W
THD + N	Total harmonic distortion + noise	$P_o = 850mW$ rms, $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.5		%
$PSRR_{IG}$	Power supply rejection ratio with inputs grounded <sup>(1)</sup>	$F = 217Hz$ , $R = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ripple} = 200mV_{PP}$	75 <sup>(2)</sup>	90		dB
CMRR	Common mode rejection ratio	$F = 217Hz$ , $R_L = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ic} = 200mV_{PP}$		60		dB
SNR	Signal-to-noise ratio	<b>A-weighted filter</b> $R_L = 8\Omega$ , THD + N < 0.7%, $20Hz \leq F \leq 20kHz$		100		dB
GBP	Gain bandwidth product	$R_L = 8\Omega$		2		MHz
$V_N$	Output voltage noise	<b><math>20Hz \leq F \leq 20kHz</math>, <math>R_L = 8\Omega</math></b> Unweighted A-weighted Unweighted, standby A-weighted, standby		11 7 3.5 1.5		$\mu V_{RMS}$
$Z_{in}$	Input impedance		15	20	25	k $\Omega$
-	Gain mismatch		5.5	6	6.5	dB
$t_{WU}$	Wake-up time <sup>(3)</sup>	$C_b = 1\mu F$		15		ms

1. Dynamic measurements -  $20 \cdot \log(\text{rms}(V_{out})/\text{rms}(V_{ripple}))$ .  $V_{ripple}$  is the super-imposed sinus signal relative to  $V_{CC}$ .

2. Guaranteed by design and evaluation.

3. Transition time from standby mode to fully operational amplifier.

**Table 5.**  $V_{CC} = +3.3V$  (all electrical values are guaranteed with correlation measurements at 2.6V and 5V),  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)

Symbol	Parameter	Test conditions	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply current	No input signal, no load		3	7	mA
$I_{STBY}$	Standby current	No input signal, $V_{STBY} = V_{SM} = GND$ , $R_L = 8\Omega$ No input signal, $V_{STBY} = V_{SM} = V_{CC}$ , $R_L = 8\Omega$		10	1000	nA
$V_{oo}$	Differential output offset voltage	No input signal, $R_L = 8\Omega$		0.1	10	mV
$V_{IC}$	Input common mode voltage		0.4		2.3	V
$P_o$	Output power	THD = 1% max, $F = 1kHz$ , $R_L = 8\Omega$	300	500		mW
THD + N	Total harmonic distortion + noise	$P_o = 300mW$ rms, $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.5		%
$PSRR_{IG}$	Power supply rejection ratio with inputs grounded <sup>(1)</sup>	$F = 217Hz$ , $R = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ripple} = 200mV_{PP}$	75 <sup>(2)</sup>	90		dB
CMRR	Common mode rejection ratio	$F = 217Hz$ , $R_L = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ic} = 200mV_{PP}$		60		dB
SNR	Signal-to-noise ratio	<b>A-weighted filter</b> $R_L = 8\Omega$ , THD + N < 0.7%, $20Hz \leq F \leq 20kHz$		100		dB
GBP	Gain bandwidth product	$R_L = 8\Omega$		2		MHz
$V_N$	Output voltage noise	<b><math>20Hz \leq F \leq 20kHz</math>, <math>R_L = 8\Omega</math></b> Unweighted A weighted Unweighted, standby A weighted, standby		11 7 3.5 1.5		$\mu V_{RMS}$
$Z_{in}$	Input impedance		15	20	25	k $\Omega$
-	Gain mismatch		5.5	6	6.5	dB
$t_{WU}$	Wake-up time <sup>(3)</sup>	$C_b = 1\mu F$		10		ms

1. Dynamic measurements -  $20 \cdot \log(\text{rms}(V_{out})/\text{rms}(V_{ripple}))$ .  $V_{ripple}$  is the super-imposed sinus signal relative to  $V_{CC}$ .
2. Guaranteed by design and evaluation.
3. Transition time from standby mode to fully operational amplifier.

Table 6.  $V_{CC} = +2.6V$ ,  $GND = 0V$ ,  $T_{amb} = 25^{\circ}C$  (unless otherwise specified)

Symbol	Parameter	Test conditions	Min.	Typ.	Max.	Unit
$I_{CC}$	Supply current	No input signal, no load		3	7	mA
$I_{STBY}$	Standby current	No input signal, $V_{STBY} = V_{SM} = GND$ , $R_L = 8\Omega$ No input signal, $V_{STBY} = V_{SM} = V_{CC}$ , $R_L = 8\Omega$		10	1000	nA
$V_{oo}$	Differential output offset voltage	No input signal, $R_L = 8\Omega$		0.1	10	mV
$V_{IC}$	Input common mode voltage		0.6		1.5	V
$P_o$	Output power	THD = 1% max, $F = 1kHz$ , $R_L = 8\Omega$	200	300		mW
THD + N	Total harmonic distortion + noise	$P_o = 225mW$ rms, $20Hz \leq F \leq 20kHz$ , $R_L = 8\Omega$		0.5		%
PSRR <sub>IG</sub>	Power supply rejection ratio with inputs grounded <sup>(1)</sup>	$F = 217Hz$ , $R = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ripple} = 200mV_{PP}$	75 <sup>(2)</sup>	90		dB
CMRR	Common mode rejection ratio	$F = 217Hz$ , $R_L = 8\Omega$ , $C_{in} = 4.7\mu F$ , $C_b = 1\mu F$ $V_{ic} = 200mV_{PP}$		60		dB
SNR	Signal-to-noise ratio	<b>A-weighted filter</b> $R_L = 8\Omega$ , THD + N < 0.7%, $20Hz \leq F \leq 20kHz$		100		dB
GBP	Gain bandwidth product	$R_L = 8\Omega$		2		MHz
$V_N$	Output voltage noise	<b>20Hz <math>\leq F \leq</math> 20kHz, <math>R_L = 8\Omega</math></b> Unweighted A weighted Unweighted, standby A weighted, standby		11 7 3.5 1.5		$\mu V_{RMS}$
$Z_{in}$	Input impedance		15	20	25	k $\Omega$
-	Gain mismatch		5.5	6	6.5	dB
$t_{WU}$	Wake-up time <sup>(3)</sup>	$C_b = 1\mu F$		10		ms

1. Dynamic measurements -  $20 \cdot \log(\text{rms}(V_{out})/\text{rms}(V_{ripple}))$ .  $V_{ripple}$  is the super-imposed sinus signal relative to  $V_{CC}$ .

2. Guaranteed by design and evaluation.

3. Transition time from standby mode to fully operational amplifier.

Figure 2. THD+N vs. output power

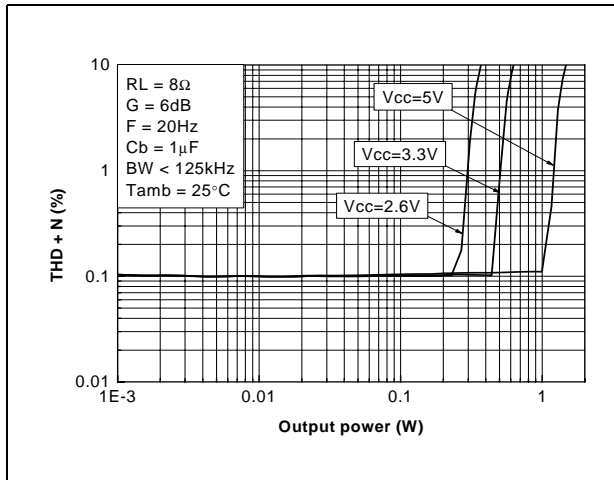


Figure 3. THD+N vs. output power

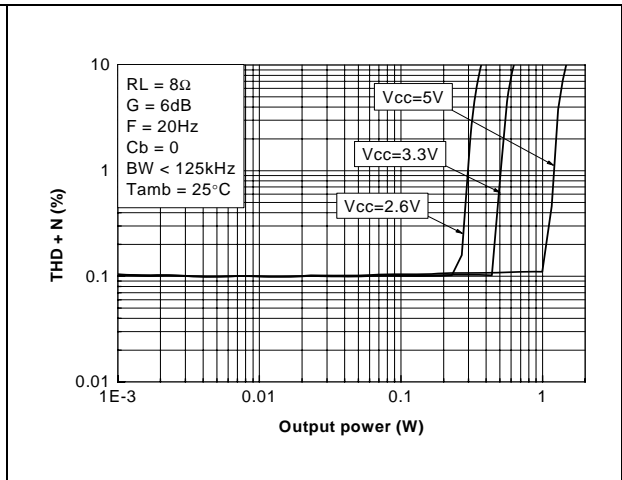


Figure 4. THD+N vs. output power

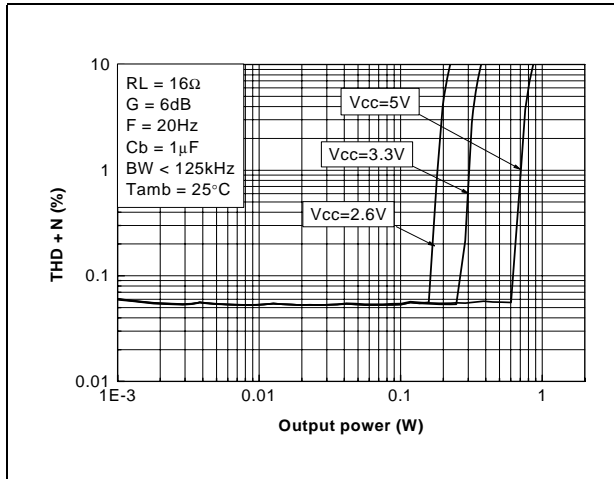


Figure 5. THD+N vs. output power

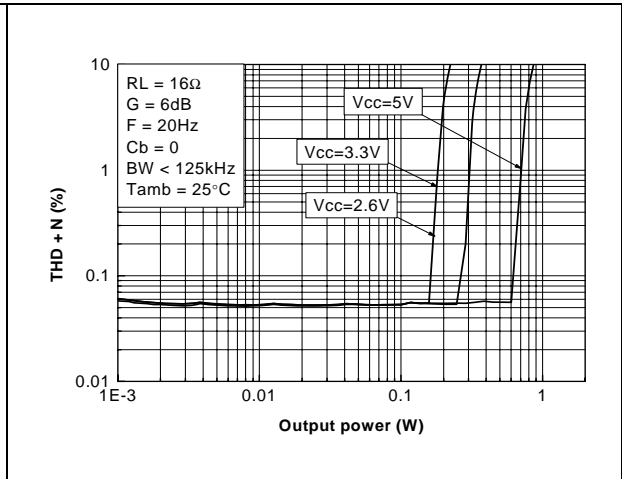


Figure 6. THD+N vs. output power

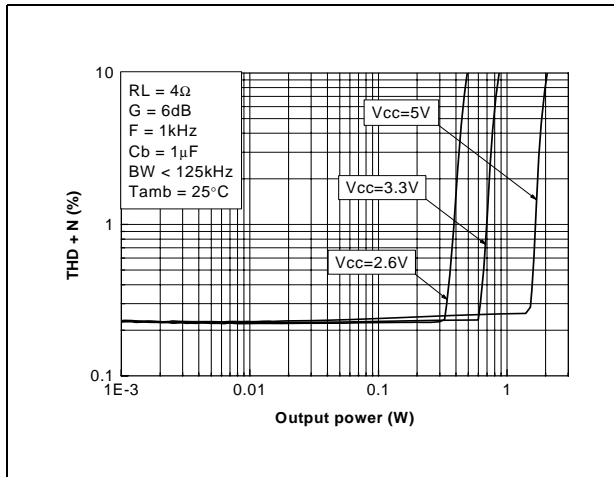


Figure 7. THD+N vs. output power

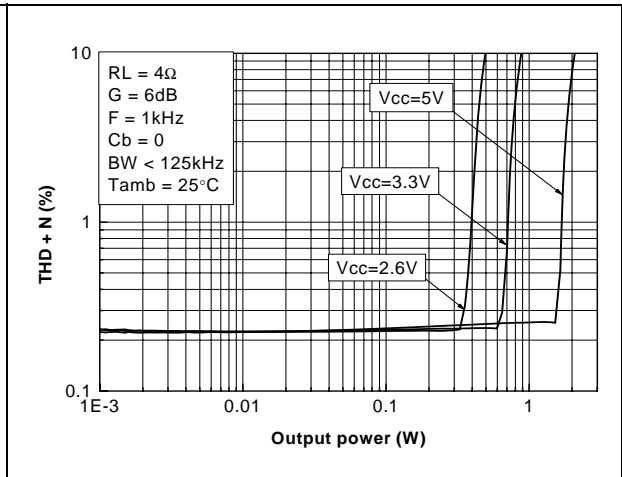




Figure 8. THD+N vs. output power

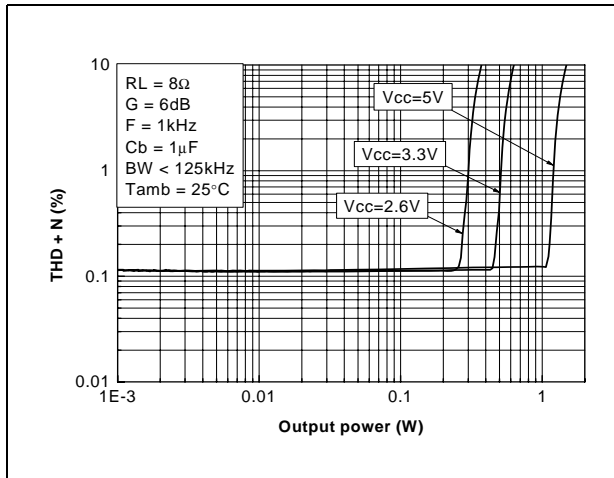


Figure 9. THD+N vs. output power

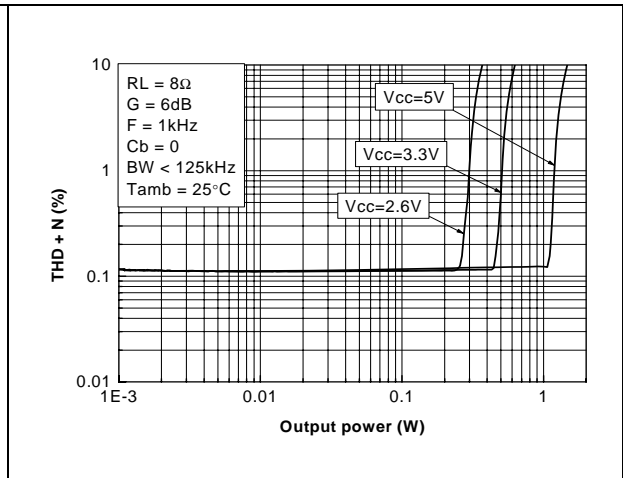


Figure 10. THD+N vs. output power

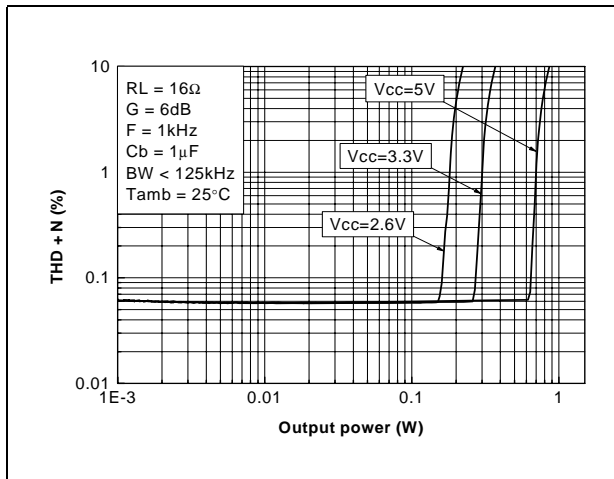


Figure 11. THD+N vs. output power

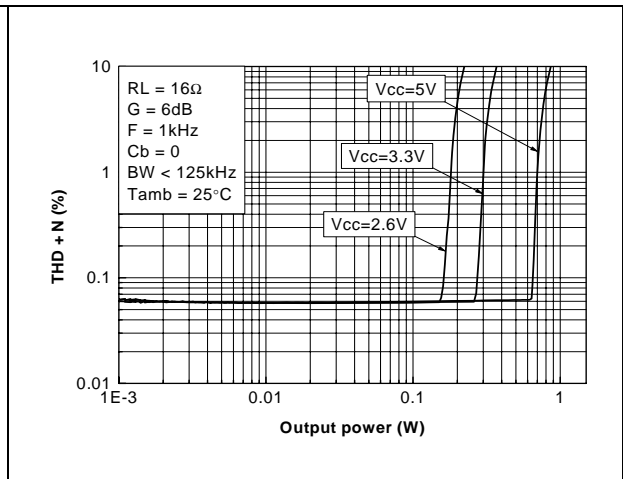


Figure 12. THD+N vs. output power

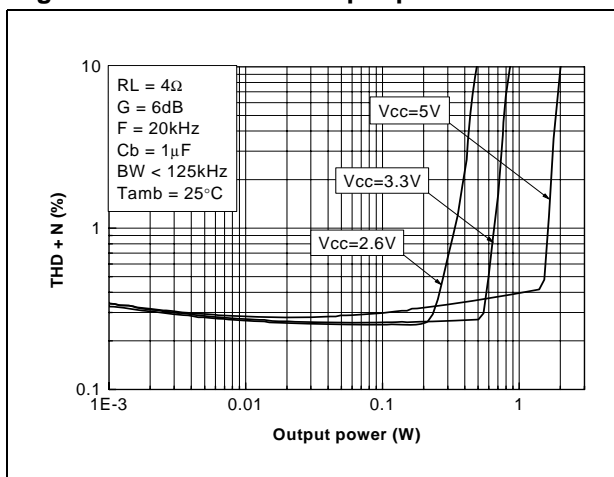


Figure 13. THD+N vs. output power

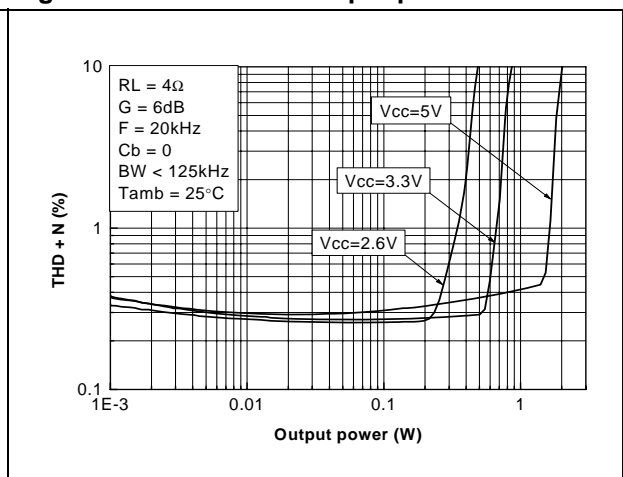


Figure 14. THD+N vs. output power

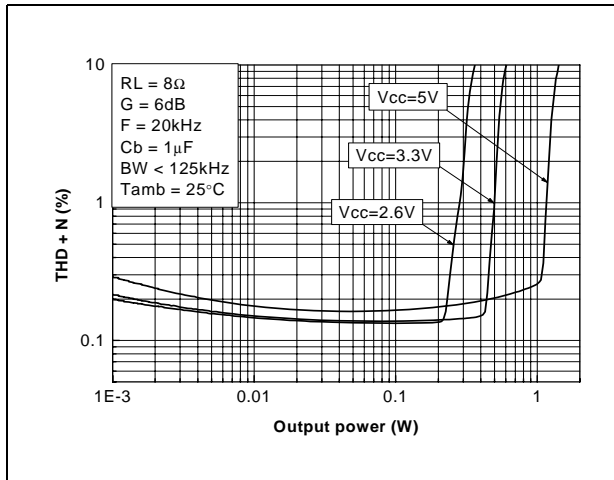


Figure 15. THD+N vs. output power

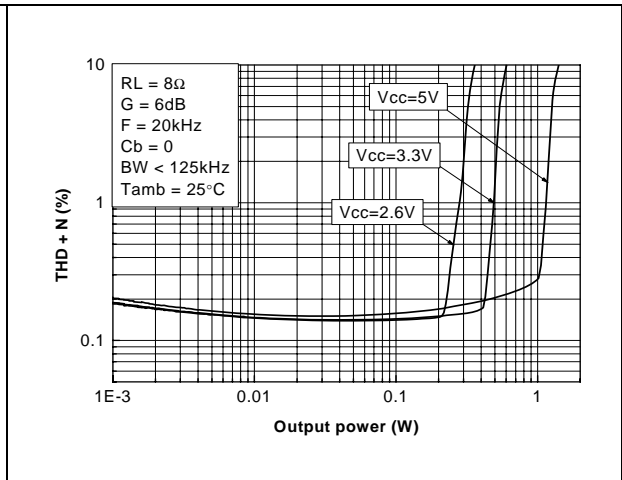


Figure 16. THD+N vs. output power

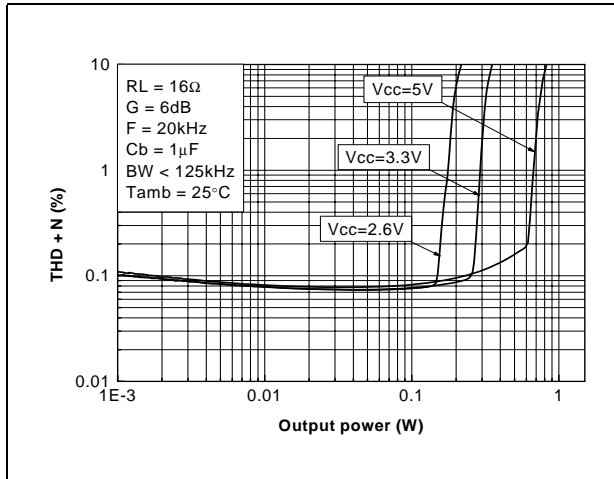


Figure 17. THD+N vs. output power

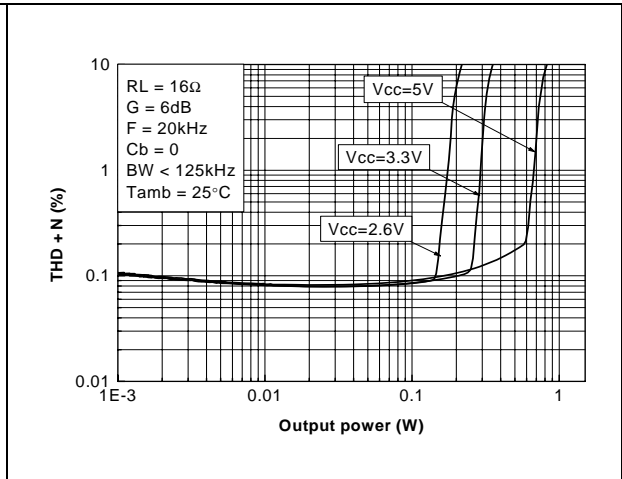


Figure 18. THD+N vs. frequency

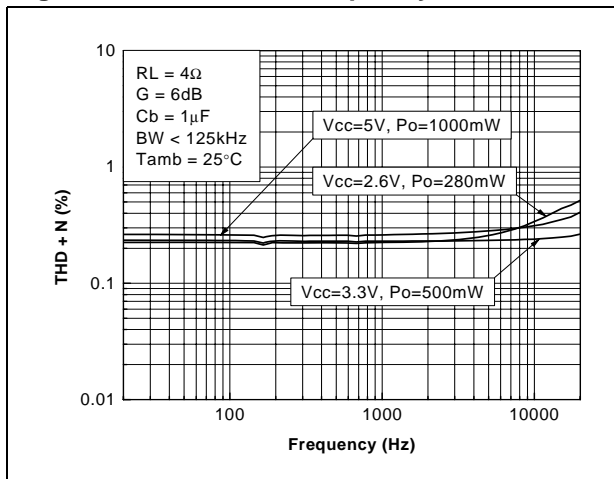


Figure 19. THD+N vs. frequency

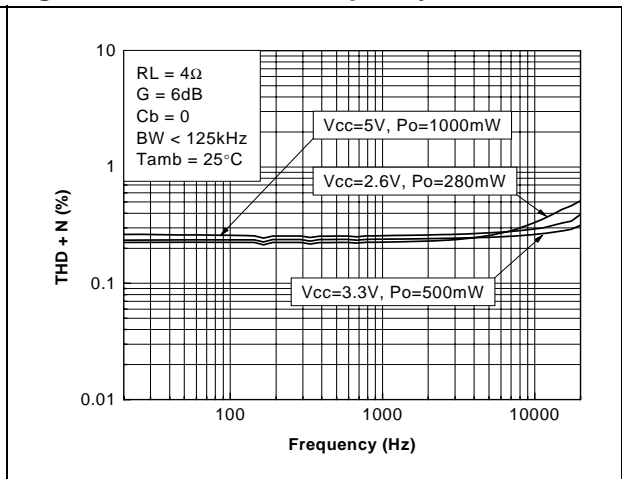


Figure 20. THD+N vs. frequency

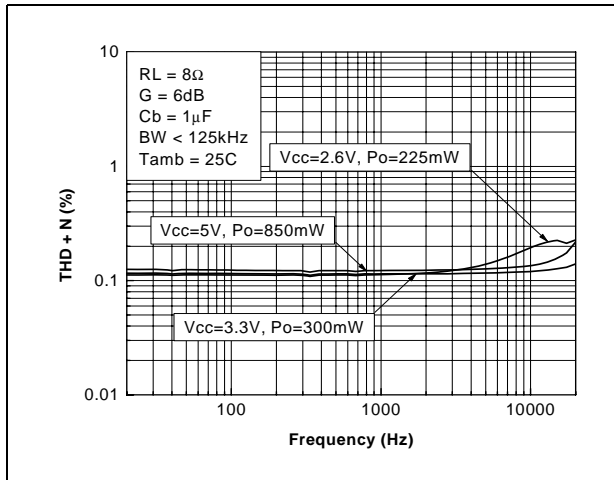


Figure 21. THD+N vs. frequency

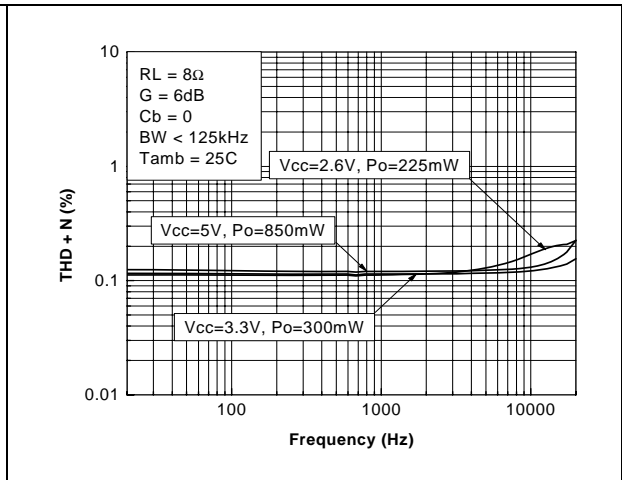


Figure 22. THD+N vs. frequency

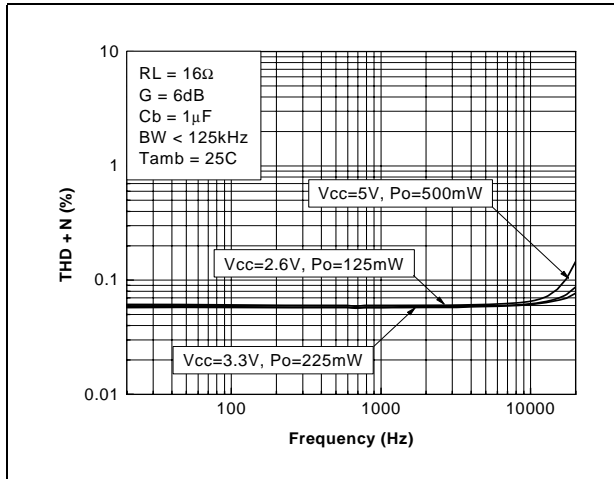


Figure 23. THD+N vs. frequency

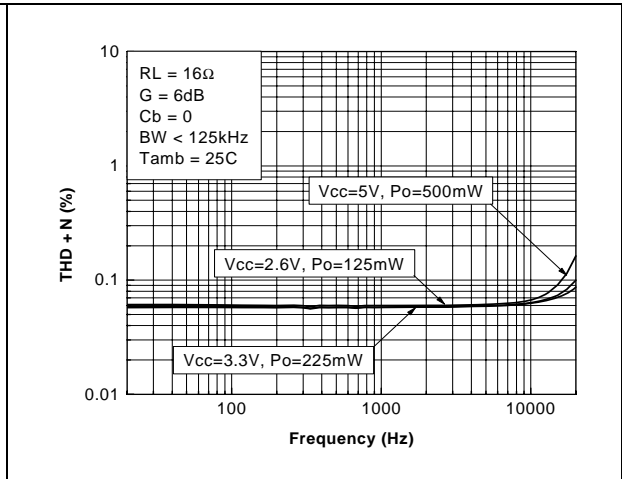


Figure 24. Output power vs. power supply voltage

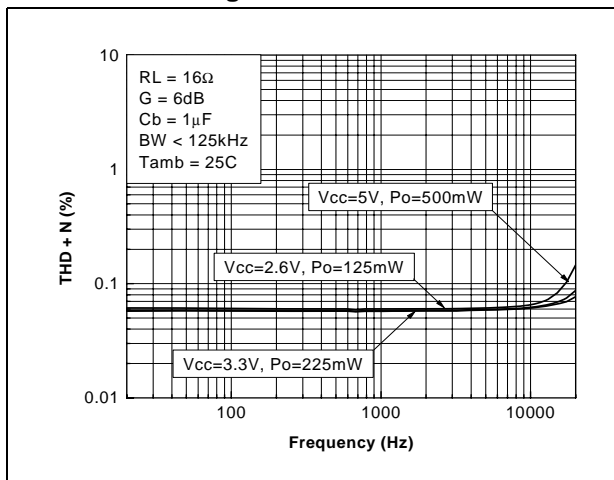


Figure 25. Output power vs. power supply voltage

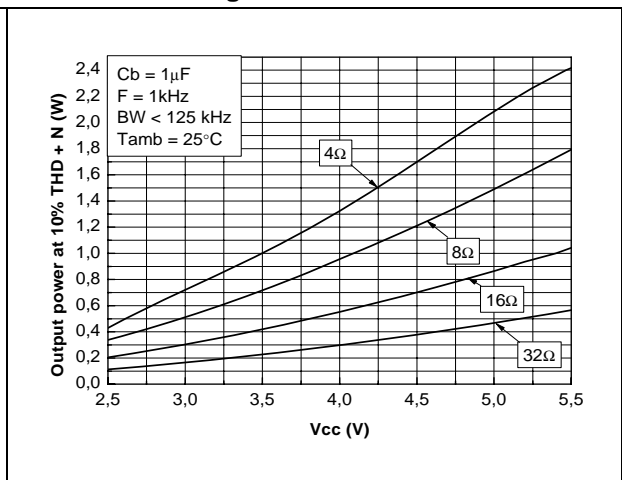


Figure 26. Output power vs. power supply voltage

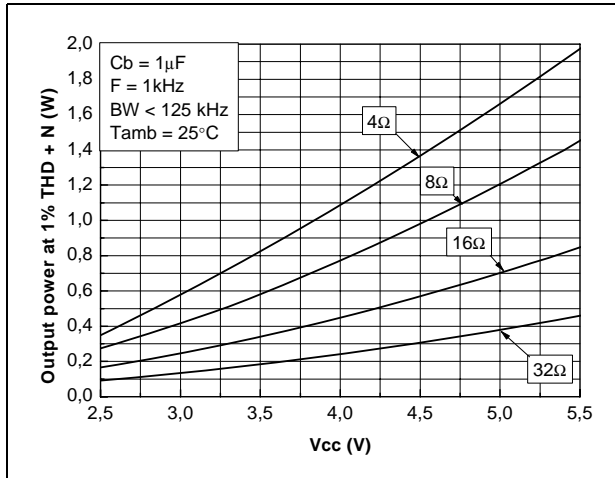


Figure 27. Power derating curves

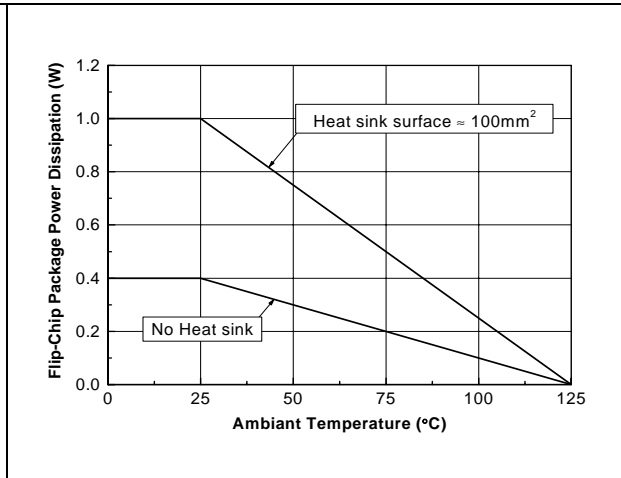


Figure 28. Output power vs. load resistance

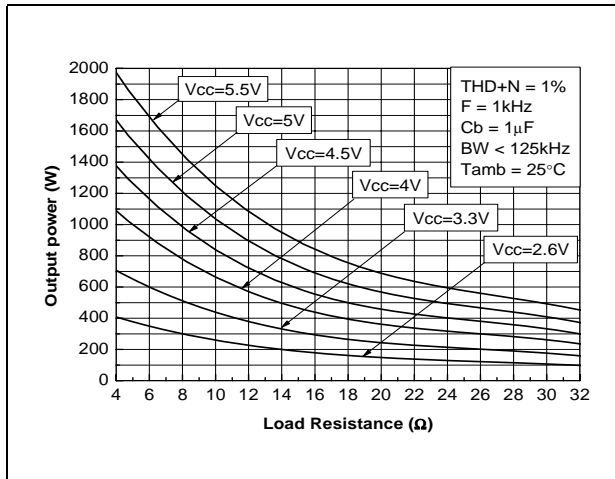


Figure 29. Power dissipation vs. output power

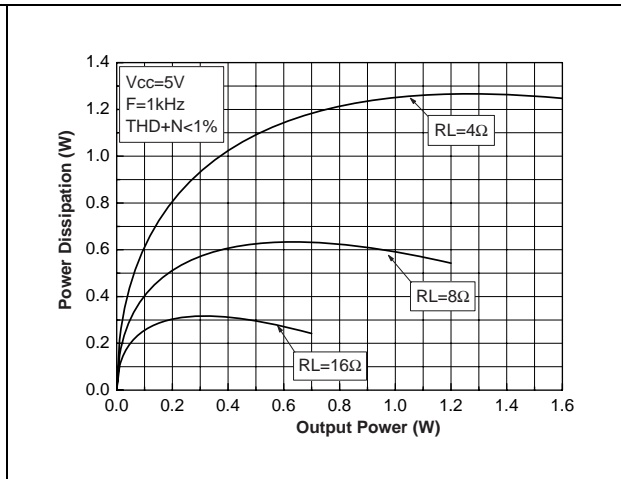


Figure 30. Power dissipation vs. output power

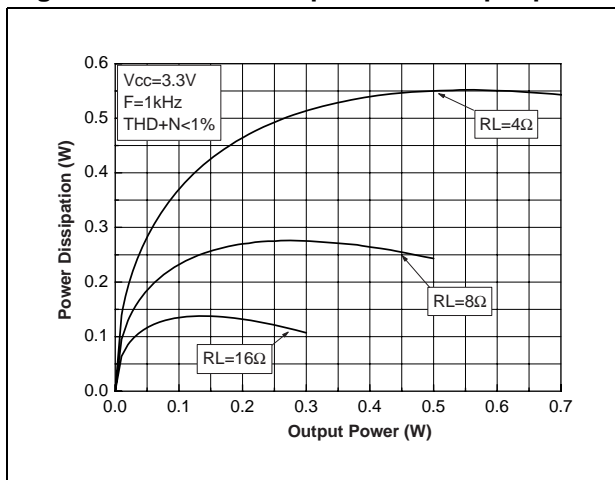


Figure 31. Power dissipation vs. output power

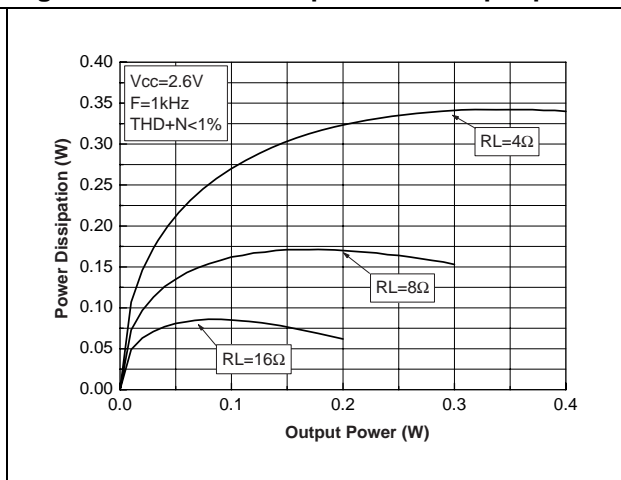


Figure 32. PSSR vs. frequency

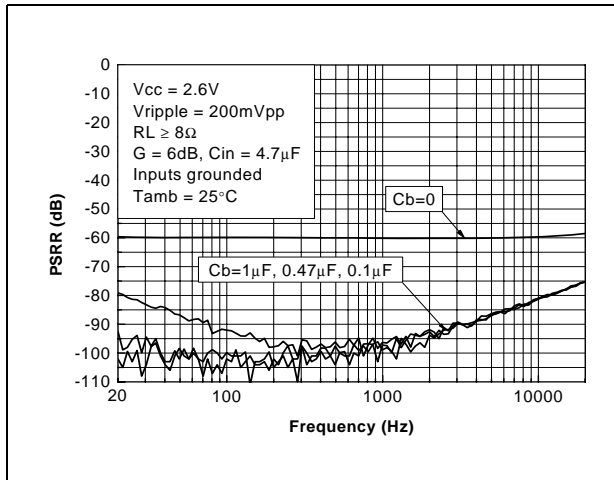


Figure 33. PSSR vs. frequency

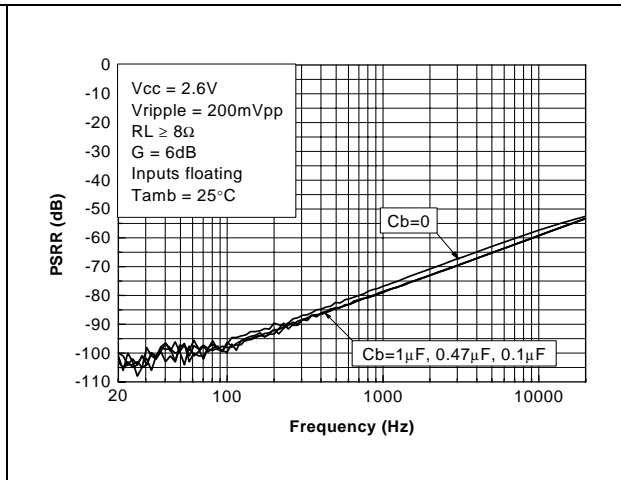


Figure 34. PSSR vs. frequency

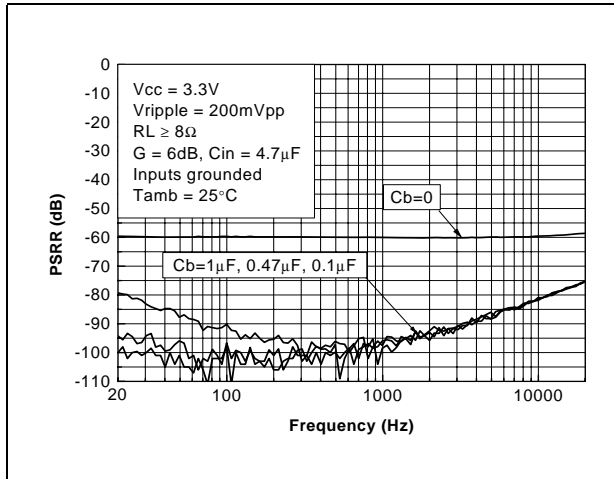


Figure 35. PSSR vs. frequency

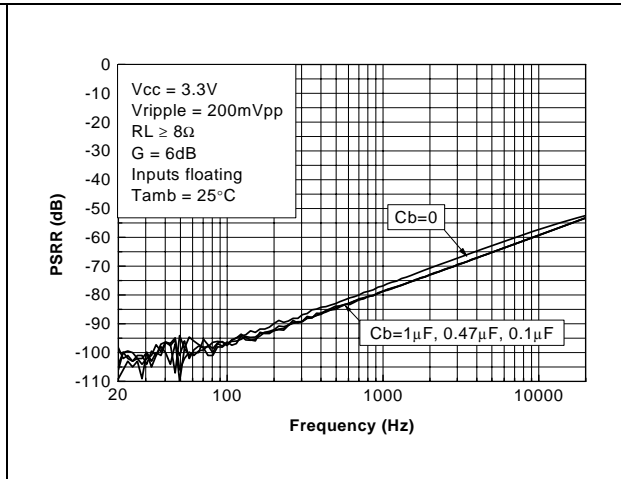


Figure 36. PSSR vs. frequency

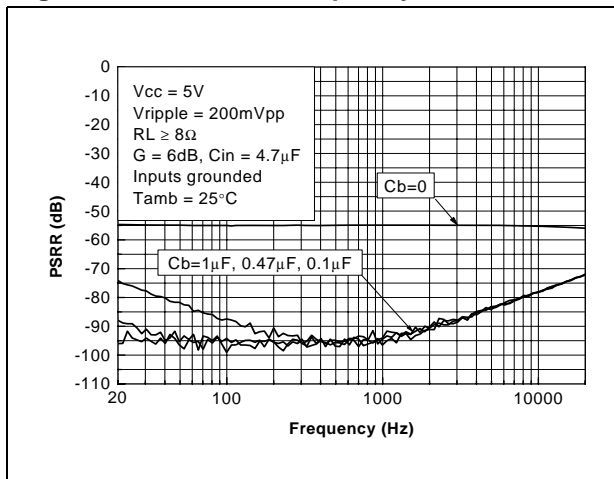


Figure 37. PSSR vs. frequency

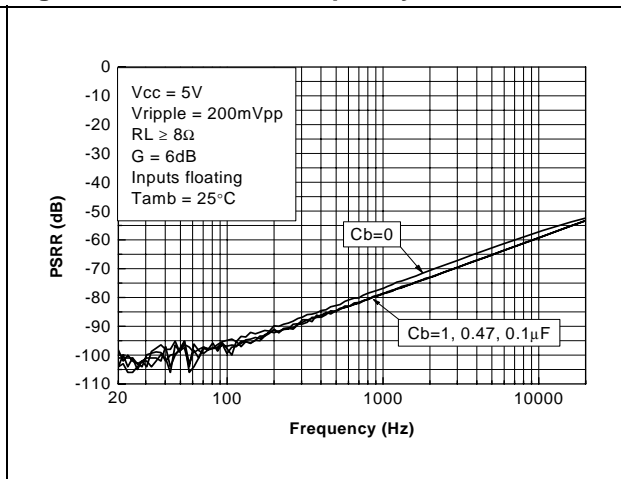


Figure 38. PSSR vs. common mode input voltage

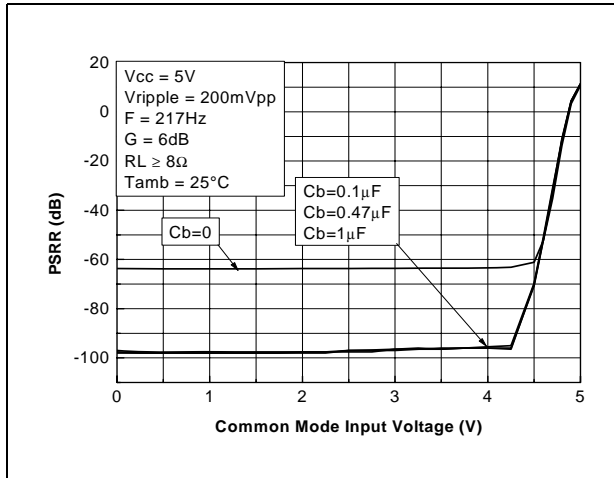


Figure 39. PSSR vs. common mode input voltage

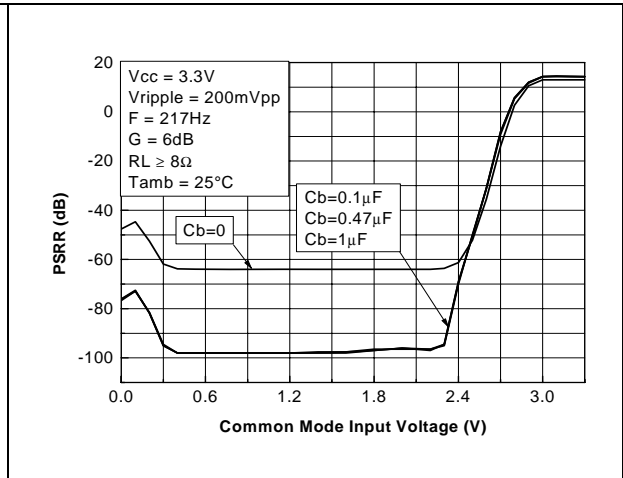


Figure 40. PSSR vs. common mode input voltage

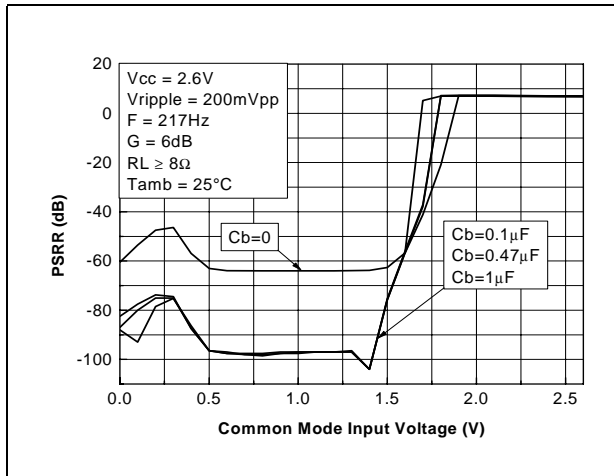


Figure 41. CMRR vs. frequency

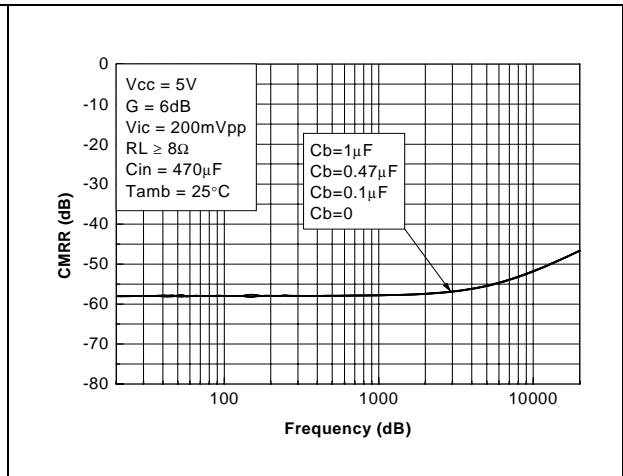


Figure 42. CMRR vs. frequency

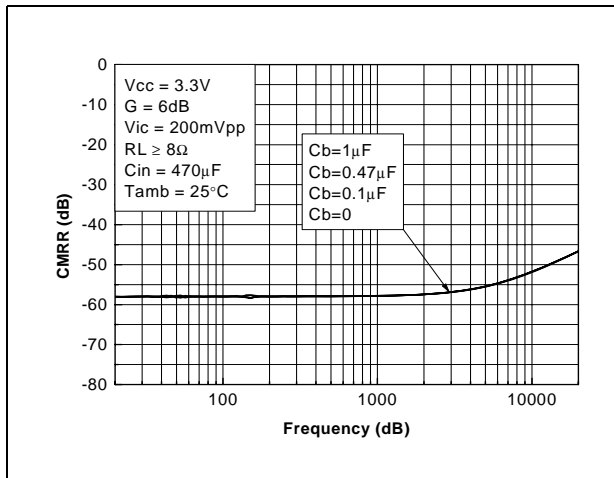


Figure 43. CMRR vs. frequency

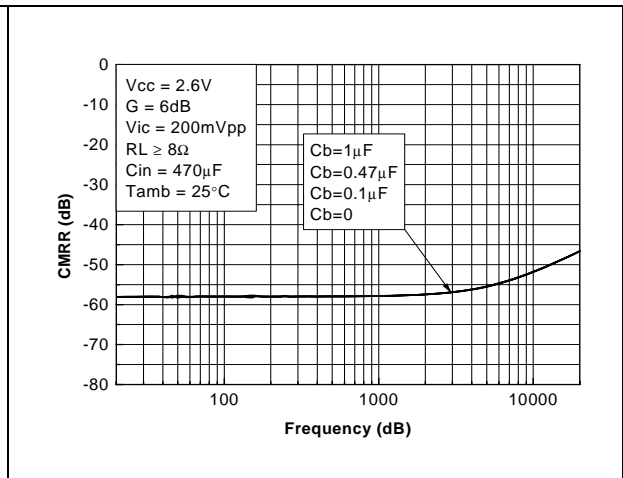


Figure 44. CMRR vs. common mode input voltage

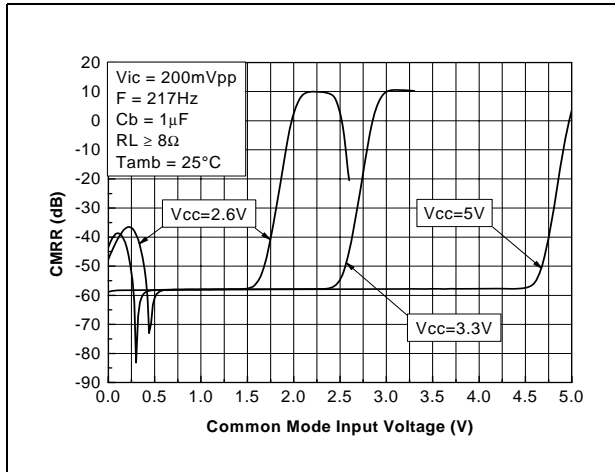


Figure 45. CMRR vs. common mode input voltage

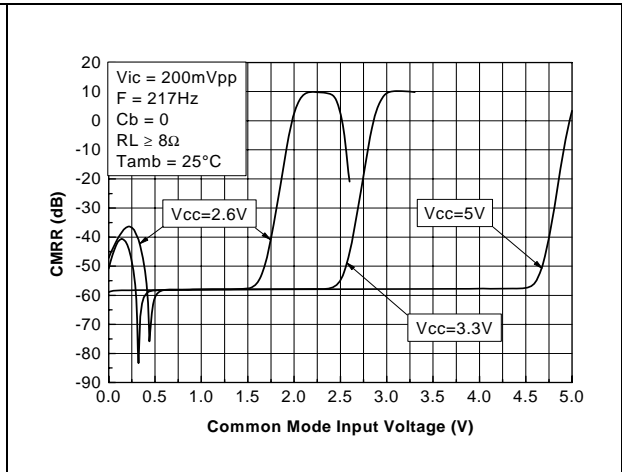


Figure 46. Current consumption vs. power supply voltage

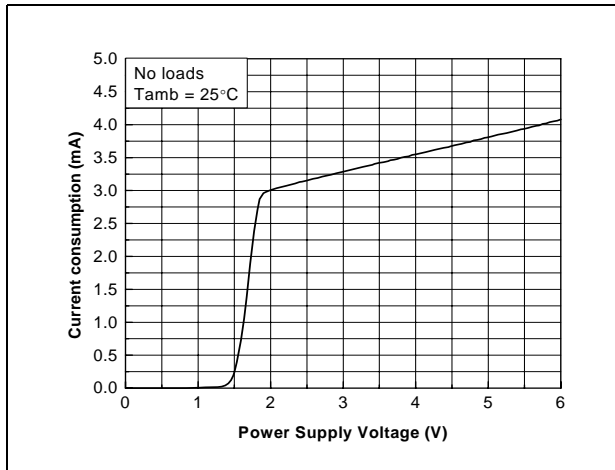


Figure 47. Differential DC output voltage vs. common mode input voltage

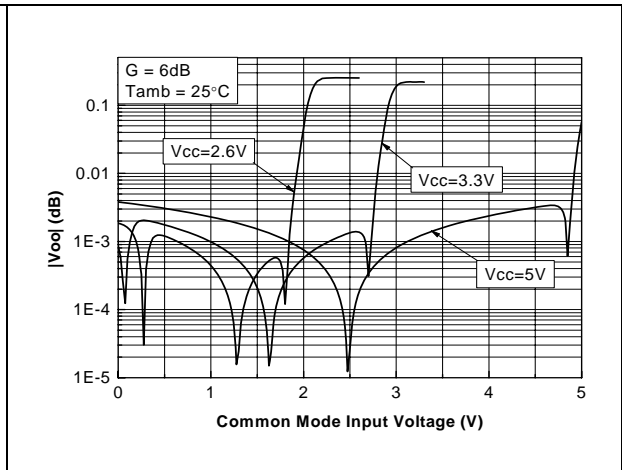


Figure 48. Current consumption vs. standby voltage

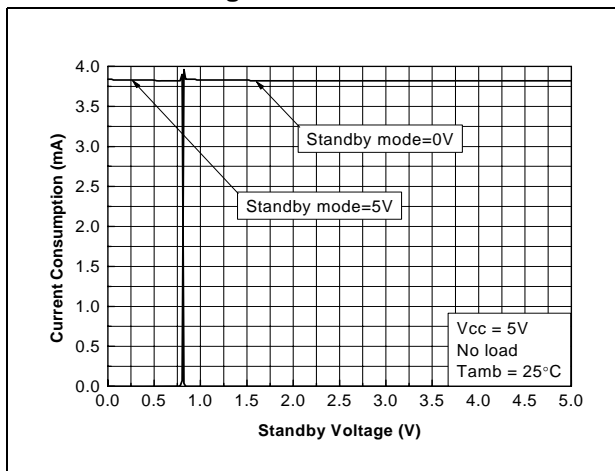


Figure 49. Current consumption vs. standby voltage

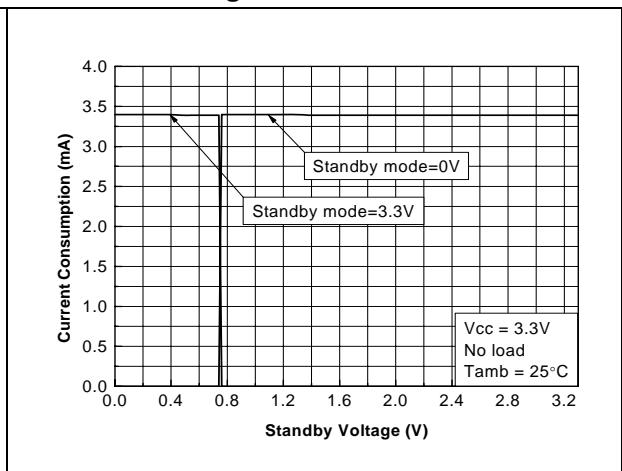


Figure 50. Current consumption vs. standby voltage

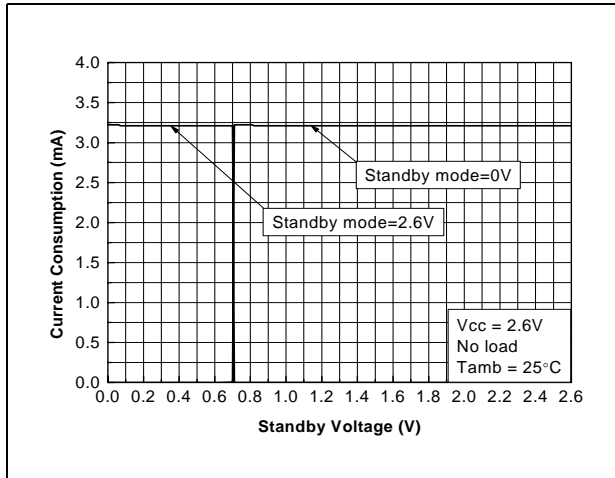


Figure 51. Frequency response

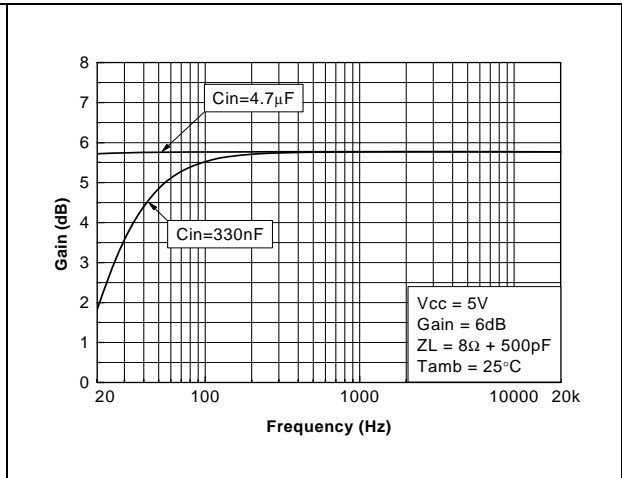


Figure 52. Frequency response

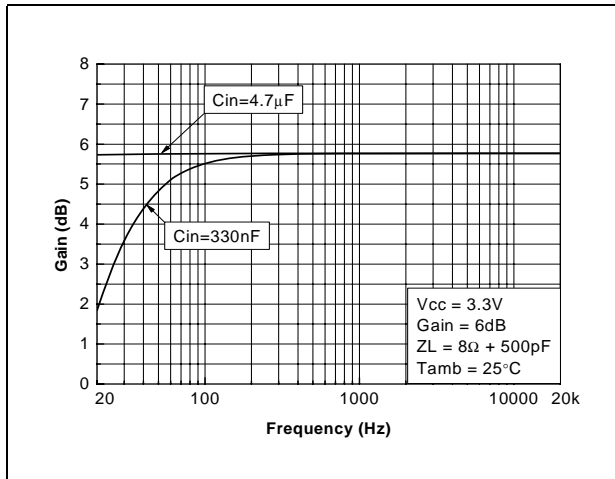


Figure 53. Frequency response

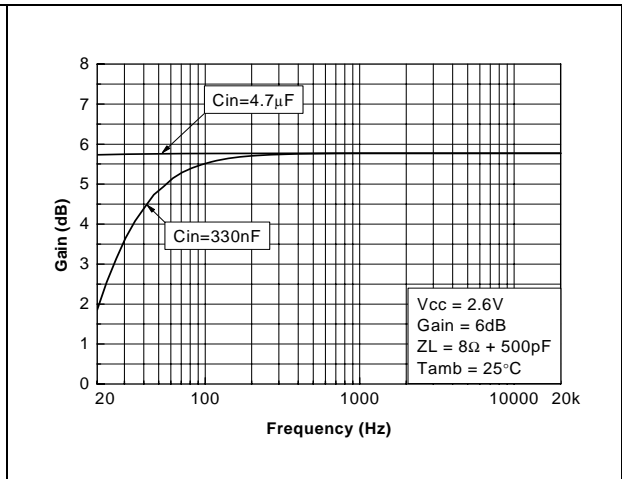


Figure 54. SNR vs. power supply voltage with unweighted filter

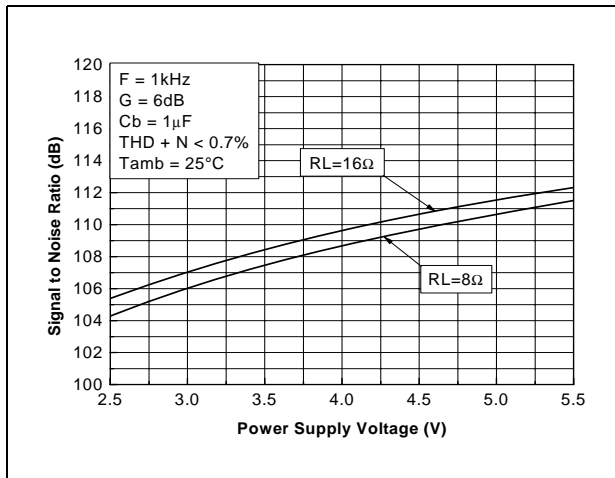
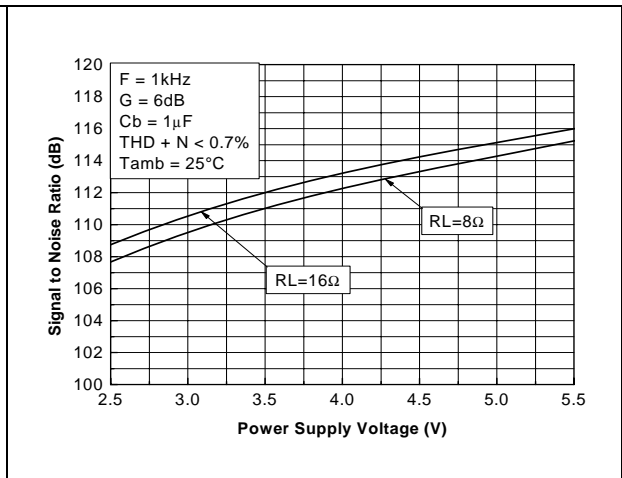


Figure 55. SNR vs. power supply voltage with A-weighted filter





## 4 Application information

### 4.1 Differential configuration principle

The TS4995 is a monolithic full-differential input/ output power amplifier with fixed +6 dB gain. The TS4995 also includes a common mode feedback loop that controls the output bias value to average it at  $V_{CC}/2$  for any DC common mode input voltage. This allows maximum output voltage swing, and therefore, to maximize the output power. Moreover, as the load is connected differentially instead of single-ended, output power is four times higher for the same power supply voltage.

The **advantages** of a full-differential amplifier are:

- Very high PSRR (power supply rejection ratio)
- High common mode noise rejection
- Virtually no pop and click without additional circuitry, giving a faster start-up time compared to conventional single-ended input amplifiers
- Easier interfacing with differential output audio DAC
- No input coupling capacitors required due to common mode feedback loop

In theory, the filtering of the internal bias by an external bypass capacitor is not necessary. However, to reach maximum performance in all tolerance situations, it is recommended to keep this option.

### 4.2 Common mode feedback loop limitations

As explained previously, the common mode feedback loop allows the output DC bias voltage to be averaged at  $V_{CC}/2$  for any DC common mode bias input voltage.

Due to the  $V_{IC}$  limitation of the input stage (see [Table 4 on page 5](#)), the common mode feedback loop can fulfil its role only within the defined range.

### 4.3 Low frequency response

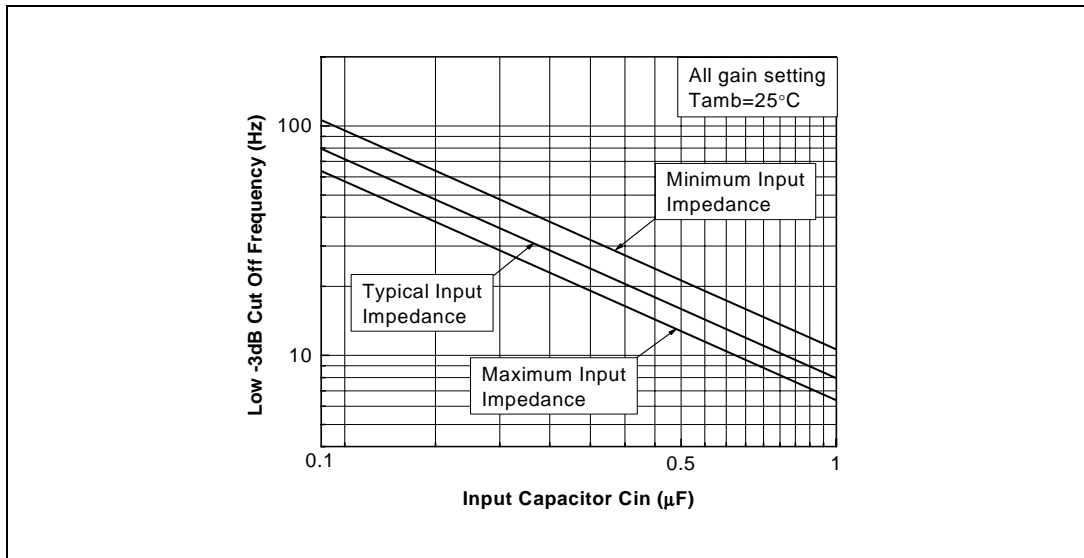
The input coupling capacitors block the DC part of the input signal at the amplifier inputs.  $C_{in}$  and  $R_{in}$  form a first-order high pass filter with -3 dB cut-off frequency.

$$F_{CL} = \frac{1}{2 \times \pi \times R_{in} \times C_{in}} \quad (\text{Hz})$$

*Note:* The input impedance for the TS4995 is typically 20k $\Omega$  and there is tolerance around this value.

From [Figure 56](#), you can easily establish the  $C_{in}$  value required for a -3 dB cut-off frequency.

Figure 56. -3 dB lower cut-off frequency vs. input capacitance



#### 4.4 Power dissipation and efficiency

**Assumptions:**

- Load voltage and current are sinusoidal ( $V_{out}$  and  $I_{out}$ )
- Supply voltage is a pure DC source ( $V_{CC}$ )

The output voltage is:

$$V_{out} = V_{peak} \sin\omega t \text{ (V)}$$

and

$$I_{out} = \frac{V_{out}}{R_L} \text{ (A)}$$

and

$$P_{out} = \frac{V_{peak}^2}{2R_L} \text{ (W)}$$

Therefore, the average current delivered by the supply voltage is:

**Equation 1**

$$I_{CC \text{ AVG}} = 2 \frac{V_{peak}}{\pi R_L} \text{ (A)}$$

The power delivered by the supply voltage is:

**Equation 2**

$$P_{supply} = V_{CC} I_{CC \text{ AVG}} \text{ (W)}$$

Therefore, the **power dissipated by each amplifier** is:

$$P_{\text{diss}} = P_{\text{supply}} - P_{\text{out}} \text{ (W)}$$

$$P_{\text{diss}} = \frac{2\sqrt{2}V_{\text{CC}}}{\pi\sqrt{R_{\text{L}}}} \sqrt{P_{\text{out}}} - P_{\text{out}}$$

and the maximum value is obtained when:

$$\frac{\partial P_{\text{diss}}}{\partial P_{\text{out}}} = 0$$

and its value is:

### Equation 3

$$P_{\text{dissmax}} = \frac{2V_{\text{CC}}^2}{\pi^2 R_{\text{L}}} \text{ (W)}$$

*Note:* This maximum value is only dependent on the power supply voltage and load values.

The **efficiency** is the ratio between the output power and the power supply:

### Equation 4

$$\eta = \frac{P_{\text{out}}}{P_{\text{supply}}} = \frac{\pi V_{\text{peak}}}{4V_{\text{CC}}}$$

The maximum theoretical value is reached when  $V_{\text{peak}} = V_{\text{CC}}$ , so:

$$\eta = \frac{\pi}{4} = 78.5\%$$

The maximum die temperature allowable for the TS4995 is 125° C. However, in case of overheating, a thermal shutdown set to 150° C, puts the TS4995 in standby until the temperature of the die is reduced by about 5° C.

To calculate the maximum ambient temperature  $T_{\text{amb}}$  allowable, you need to know:

- The power supply voltage,  $V_{\text{CC}}$
- The load resistor value,  $R_{\text{L}}$
- The package type,  $R_{\text{thja}}$

**Example:**  $V_{\text{CC}}=5 \text{ V}$ ,  $R_{\text{L}}=8 \text{ }\Omega$ ,  $R_{\text{thja-flipchip}}= 100^\circ \text{ C/W}$  (100 mm<sup>2</sup> copper heatsink).

Using the power dissipation formula given above in [Equation 3](#), this gives a result of:

$$P_{\text{dissmax}} = 633\text{mW}$$

$T_{\text{amb}}$  is calculated as follows:

### Equation 5

$$T_{\text{amb}} = 125^\circ \text{ C} - R_{\text{thja}} \times P_{\text{dissmax}}$$

Therefore, the maximum allowable value for  $T_{\text{amb}}$  is:

$$T_{\text{amb}} = 125 - 100 \times 0.633 = 61.7^\circ \text{ C}$$

### 4.5 Decoupling of the circuit

Two capacitors are needed to correctly bypass the TS4995: a power supply bypass capacitor  $C_S$  and a bias voltage bypass capacitor  $C_b$ .

The  $C_S$  capacitor has particular influence on the THD+N at high frequencies (above 7 kHz) and an indirect influence on power supply disturbances. With a value for  $C_S$  of 1  $\mu\text{F}$ , one can expect THD+N performance similar to that shown in the datasheet.

In the high frequency region, if  $C_S$  is lower than 1  $\mu\text{F}$ , then THD+N increases and disturbances on the power supply rail are less filtered.

On the other hand, if  $C_S$  is greater than 1  $\mu\text{F}$ , then those disturbances on the power supply rail are more filtered.

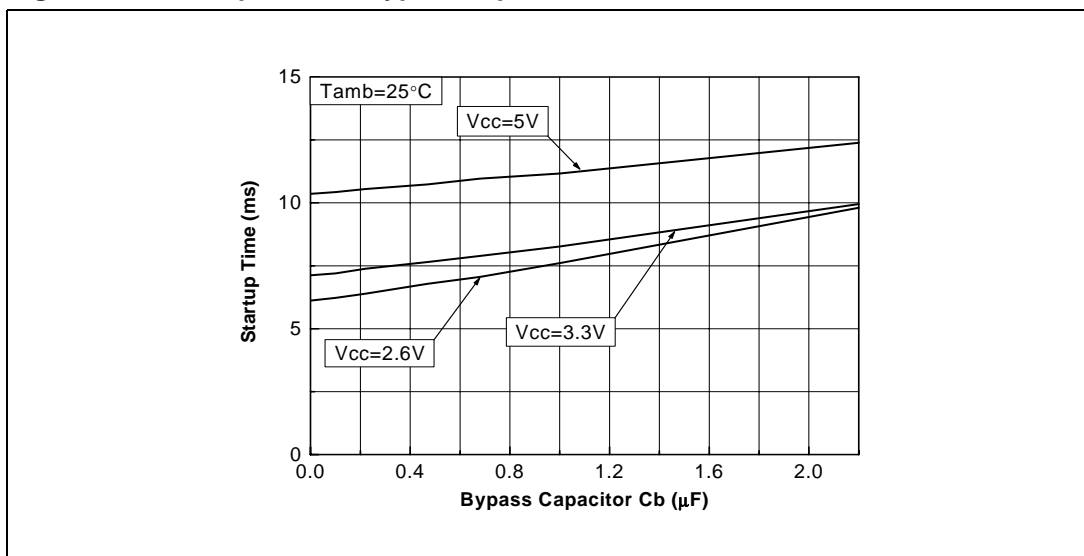
The  $C_b$  capacitor has an influence on the THD+N at lower frequencies, but also impacts PSRR performance (with grounded input and in the lower frequency region).

### 4.6 Wake-up time $t_{WU}$

When the standby is released to put the device ON, the bypass capacitor  $C_b$  is not charged immediately. Because  $C_b$  is directly linked to the bias of the amplifier, the bias will not work properly until the  $C_b$  voltage is correct. The time to reach this voltage is called the wake-up time or  $t_{WU}$  and is specified in [Table 4 on page 5](#), with  $C_b=1 \mu\text{F}$ . During the wake-up phase, the TS4995 gain is close to zero. After the wake-up time, the gain is released and set to its nominal value.

If  $C_b$  has a value different from 1  $\mu\text{F}$ , then refer to the graph in [Figure 57](#) to establish the corresponding wake-up time.

**Figure 57. Startup time vs. bypass capacitor**



## 4.7 Shutdown time

When the standby command is set, the time required to put the two output stages in high impedance and the internal circuitry in shutdown mode is a few microseconds.

*Note:* In shutdown mode, the Bypass pin and  $V_{in+}$ ,  $V_{in-}$  pins are shorted to ground by internal switches. This allows a quick discharge of  $C_b$  and  $C_{in}$ .

## 4.8 Pop performance

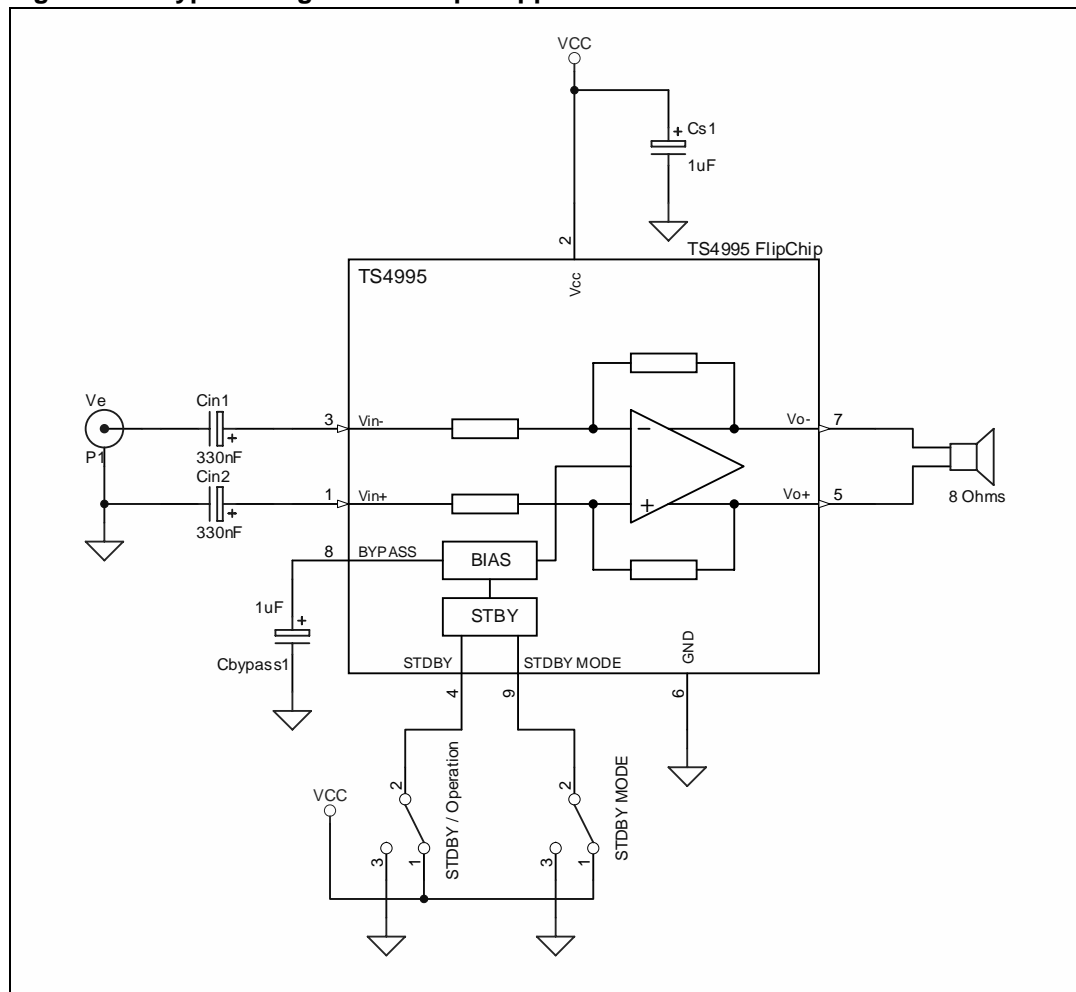
Due to its fully differential structure, the pop performance of the TS4995 is close to perfect. However, due to mismatching between internal resistors  $R_{in}$ ,  $R_{feed}$ , and external input capacitors  $C_{in}$ , some noise might remain at startup. To eliminate the effect of mismatched components, the TS4995 includes pop reduction circuitry. With this circuitry, the TS4995 is close to zero pop for all possible common applications.

In addition, when the TS4995 is in standby mode, due to the high impedance output stage in this configuration, no pop is heard.

## 4.9 Single-ended input configuration

It is possible to use the TS4995 in a single-ended input configuration. However, input coupling capacitors are needed in this configuration. The schematic diagram in [Figure 58](#) shows an example of this configuration.

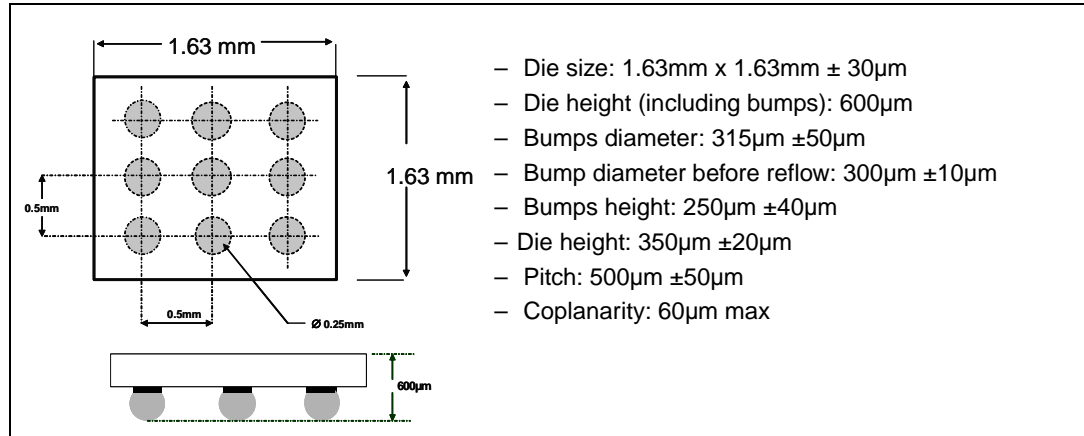
Figure 58. Typical single-ended input application



## 5 Package information

To meet environmental requirements, STMicroelectronics offers these devices in ECOPACK® packages. These packages have a lead-free second level interconnect. The category of second level interconnect is marked on the package and on the inner box label, in compliance with JEDEC Standard JESD97. The maximum ratings related to soldering conditions are also marked on the inner box label. ECOPACK is an STMicroelectronics trademark. ECOPACK specifications are available at: [www.st.com](http://www.st.com).

**Figure 59. 9-bump flip-chip package mechanical drawing**



**Figure 60. Tape and reel schematics**

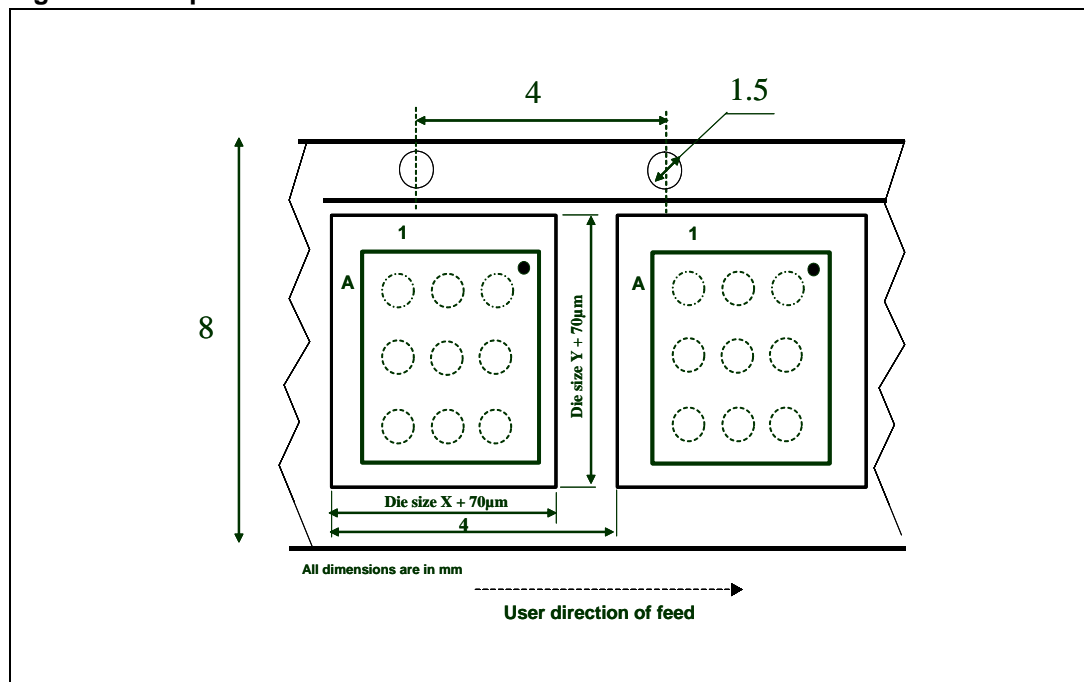


Figure 61. Pin out (top view)

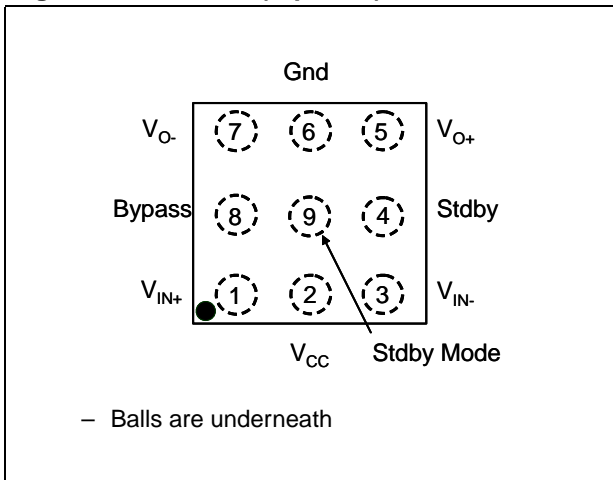
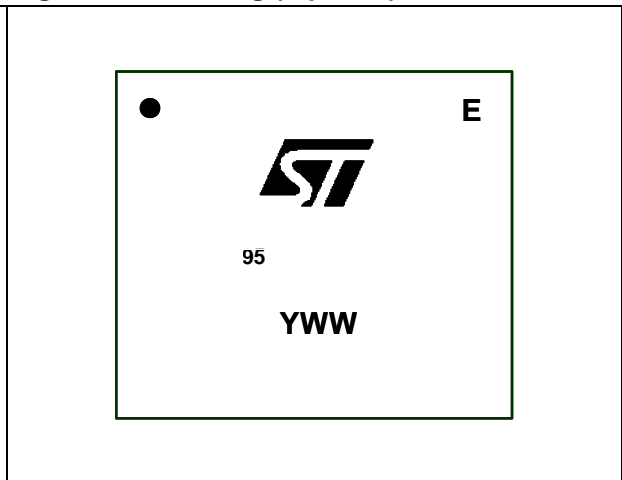


Figure 62. Marking (top view)





## 6 Ordering information

Table 7. Order code

Order code	Temperature range	Package	Packing	Marking
TS4995EIJT	-40° C to +85° C	Lead free flip chip 9	Tape & reel	95

## 7 Revision history

Table 8. Document revision history

Date	Revision	Changes
1-Jun-2006	1	Final datasheet.
25-Oct-2006	2	Additional information for 4Ω load.
25-Mar-2008	3	Modified <i>Figure 60: Tape and reel schematics</i> to correct die orientation.

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